

2A 18V Synchronous PFM/PWM Step-Down Regulator

ABSOLUTE MAXIMUM RATINGS

These are stress ratings only and functional operation of the device at these ratings or any other above those indicated in the operation sections of the specifications below is not implied. Exposure to absolute maximum rating conditions for extended periods of time may affect reliability.

Supply Voltage V_{IN} -0.3V to 20V
 Switch Node Voltage V_{SW} 21V
 Boost Voltage V_{BS} -0.3 to $V_{SW}+6V$
 Enable Voltage V_{EN} -0.3 to V_{IN}
 All Other Pins -0.3 to +6V
 Junction Temperature 150°C
 Storage Temperature -65°C to 150°C
 Lead Temperature (Soldering, 10 sec) 260°C
 ESD Rating (HBM - Human Body Model) 2kV
 ESD Rating (MM - Machine Model) 200V
 Moisture Sensitivity Level (MSL) 3

OPERATING RATINGS

Input Voltage V_{IN} 4.5V to 18V
 Ambient Operating Temperature -40°C to 85°C
 Maximum Output Current 2A min
 Thermal Resistance θ_{JA} 105°C/W

ELECTRICAL SPECIFICATIONS

Specifications are for an Operating Ambient Temperature of $T_A = 25^\circ\text{C}$ only; limits applying over the full Ambient Operating Temperature range are denoted by a "•". Minimum and Maximum limits are guaranteed through test, design, or statistical correlation. Typical values represent the most likely parametric norm at $T_A = 25^\circ\text{C}$, and are provided for reference purposes only. Unless otherwise indicated, $V_{IN} = V_{EN} = 12V$, $V_{OUT}=3.3V$.

Parameter	Min.	Typ.	Max.	Units	Conditions
Shutdown Supply Current		0.1	10	μA	$V_{EN}=0V$
Quiescent Current		1.2	1.4	mA	$V_{EN}=3V$, $V_{FB}=1V$
Feedback Voltage V_{FB}	0.907	0.925	0.943	V	
Feedback Overvoltage Threshold		1.1		V	
Feedback Bias Current	-0.1		0.1	μA	$V_{FB}=1V$
Error Amplifier Voltage Gain A_{EA} ¹		400		V/V	
Error Amplifier Transconductance G_{EA}		800		$\mu\text{A/V}$	
COMP to Current Sense Transconductance G_{CS}		3.5		A/V	
High-Side switch On Resistance $R_{DS(ON)H}$ ²		100		m Ω	$I_{SW}=0.2A\&0.7A$
Low-Side switch On Resistance $R_{DS(ON)L}$ ²		100		m Ω	$I_{SW}=-0.2A\&-0.7A$
High-Side switch Leakage Current		0.1	10	μA	$V_{IN}=18V$, $V_{EN}=0V$, $V_{SW}=0V$
High-Side Switch Current Limit	2.7	3.5		A	
Low-Side Switch Current Limit		0		A	Drain to Source
Oscillator Frequency F_{OSC1}	280	340	400	kHz	
Short Circuit Oscillator Frequency F_{OSC2}		90		kHz	
Maximum Duty Cycle D_{MAX}		90		%	$V_{FB}=0.85V$
Minimum Duty Cycle D_{MIN}			0	%	$V_{FB}=1V$
Minimum Start-up Current		10		mA	$V_{IN}\leq 4.75V$
Minimum No Load Start-up Voltage		5		V	$I_{OUT}=0A$
Minimum Full Load Start-up Voltage		4.75		V	$I_{OUT}=2A$

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Parameter	Min.	Typ.	Max.	Units		Conditions
EN Shutdown Threshold	1.1	1.5	2	V		
EN Shutdown Hysteresis ¹		0.35				
EN Lockout Threshold	2.2	2.5	2.7	V		
EN Lockout Hysteresis		0.21				
UVLO Threshold	3.65	4.00	4.25	V		V _{IN} Rising
UVLO Hysteresis		0.20		V		
Soft-start Current		5		μA		
Soft-start Time ¹		15		ms		C _{SS} =0.1μF, I _{OUT} =500mA
Thermal Shutdown ¹		160		°C		
Thermal Shutdown Hysteresis ¹		30		°C		

Note 1: Guaranteed by design.

Note 2: $R_{DS(on)} = (V_{SW1} - V_{SW2}) / (I_{SW1} - I_{SW2})$

BLOCK DIAGRAM

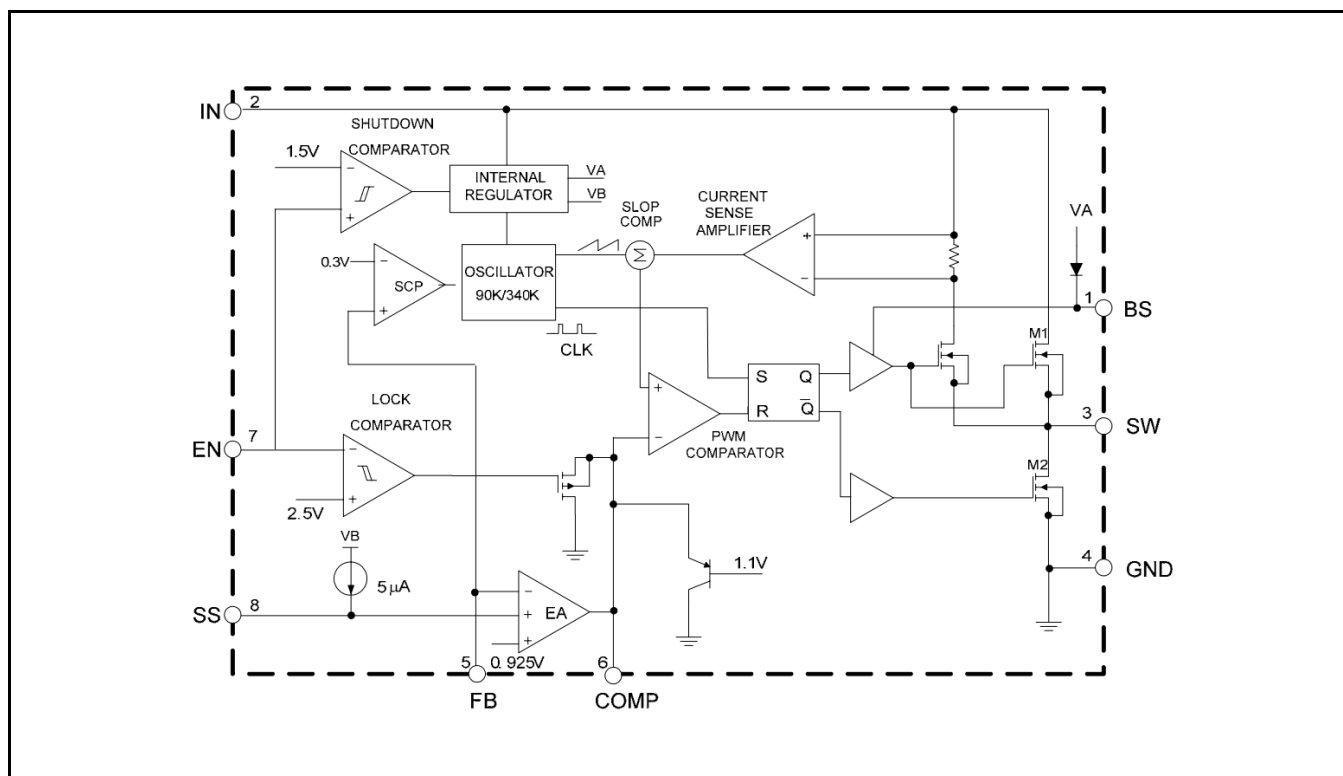


Fig. 2: XRP7674 Block Diagram

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PIN ASSIGNMENT

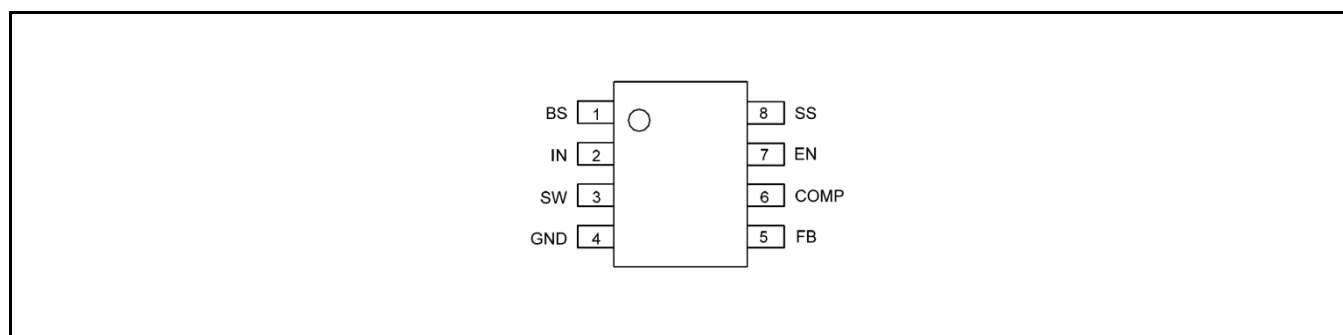


Fig. 3: XRP7674 Pin Assignment (SOIC-8)

PIN DESCRIPTION

Name	Pin Number	Description
BS	1	Bootstrap pin. Connect a 0.01 μ F or greater bootstrap capacitor between the BS pin and the SW pin. The voltage across the bootstrap capacitor drives the internal high-side power MOSFET.
IN	2	Power input pin. A capacitor should be connected between the IN pin and GND pin to keep the input voltage constant.
SW	3	Power switch output pin. This pin is connected to the inductor and the bootstrap capacitor.
GND	4	Ground pin.
FB	5	Feedback pin. An external resistor divider connected to FB programs the output voltage. If the feedback pin exceeds 1.1V the over-voltage protection will trigger. If the feedback voltage drops below 0.3V the oscillator frequency is lowered to achieve short-circuit protection.
COMP	6	Compensation pin. This is the output of transconductance error amplifier and the input to the current comparator. It is used to compensate the control loop. Connect an RC network from this pin to GND.
EN	7	Control input pin. Drive EN high/low in order to turn on/off the regulator. When the IC is in shutdown mode all functions are disabled to decrease the supply current below 1 μ A. This input can be connected to VIN (pin 2) through a 100k Ω resistor for automatic startup operations.
SS	8	Soft-start control input pin. Connect a capacitor from SS to GND to set the soft-start period. A 0.1 μ F capacitor sets the soft start period to 15ms. To disable the soft-start feature, leave SS unconnected.

ORDERING INFORMATION

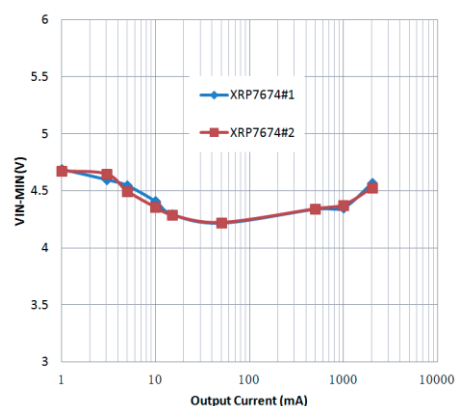
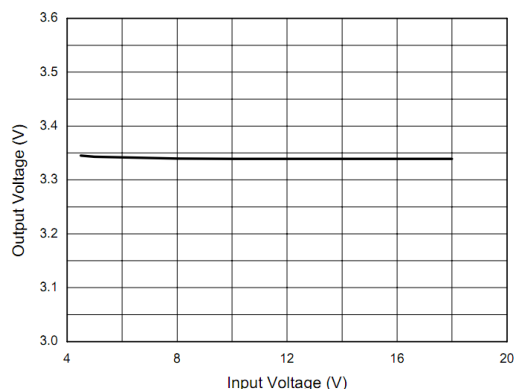
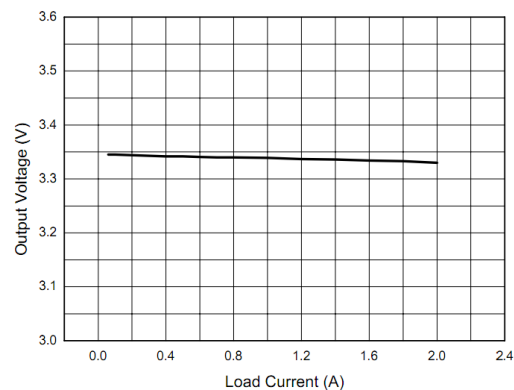
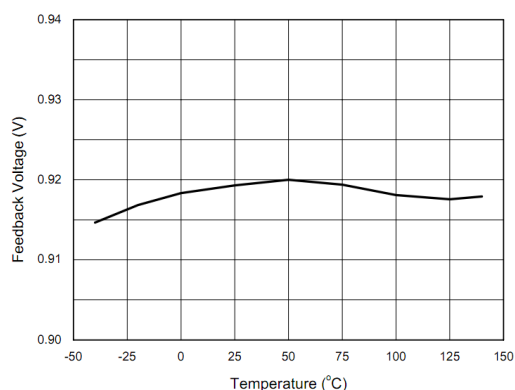
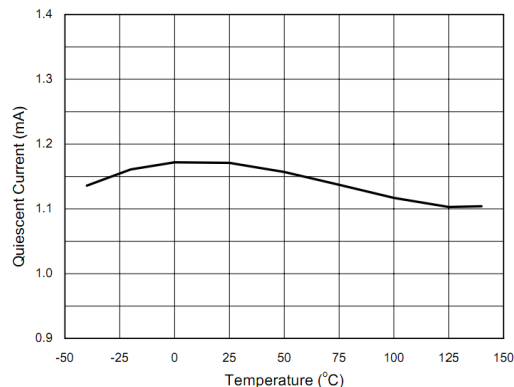
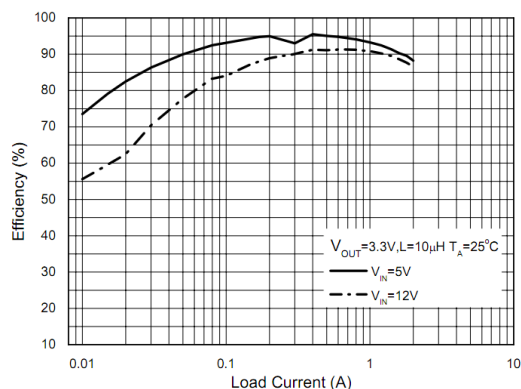
Part Number	Temperature Range	Marking	Package	Packing Quantity	Note 1	Note 2
XRP7674IDTR-F	-40°C $\leq$ T _A $\leq$ +85°C	XRP7674I YYWWF X	SOIC-8	2.5K/Tape & Reel	RoHS Compliant Halogen Free	
XRP7674EVB	XRP7674 Evaluation Board					

"YY" = Year – "WW" = Work Week – "X" = Lot Number; when applicable.

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TYPICAL PERFORMANCE CHARACTERISTICS

All data taken at $V_{IN} = 12V$, $V_{OUT} = 3.3V$, $T_J = T_A = 25^\circ C$, unless otherwise specified - Schematic and BOM from Application Information section of this datasheet.



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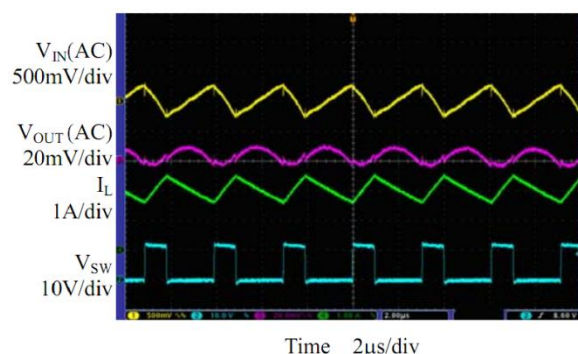


Fig. 10: Output voltage ripple
 $I_{OUT}=2A$

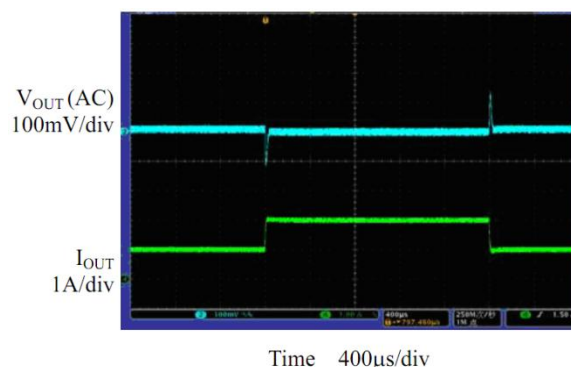


Fig. 11: Load transient
 $I_{OUT}=1A$ to $2A$

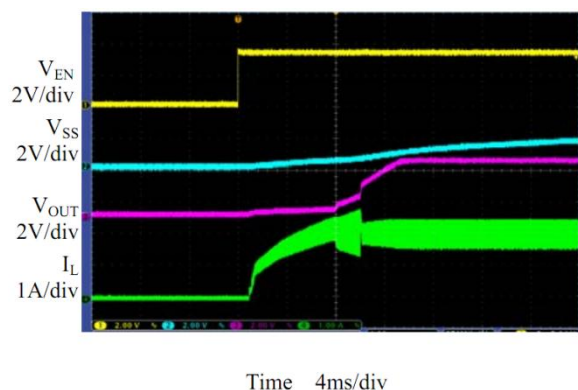


Fig. 12: Enable turn on Characteristics
 $V_{IN}=12V$, $V_{EN}=3.3V$, $V_{OUT}=3.3V$, $I_{OUT}=2A$

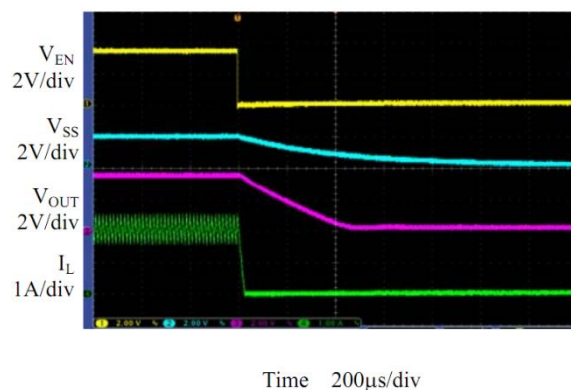


Fig. 13: Enable turn off
 $V_{IN}=12V$, $V_{EN}=3.3V$, $V_{OUT}=3.3V$, $I_{OUT}=2A$

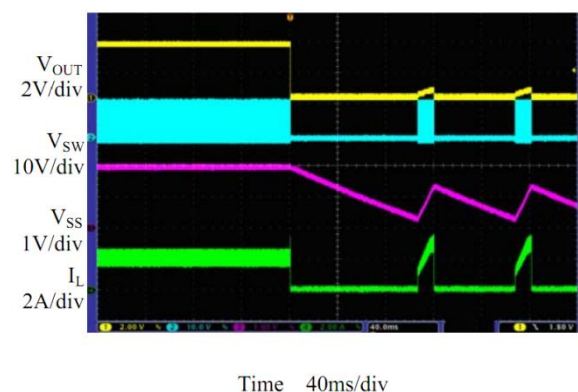


Fig. 14: Short-circuit protection
 $I_{OUT}=2A$

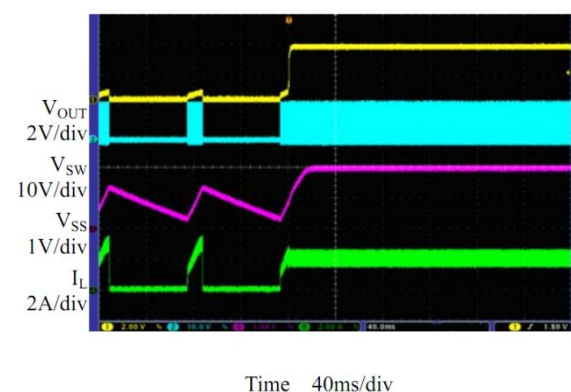


Fig. 15: Short-circuit recovery
 $I_{OUT}=2A$

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THEORY OF OPERATION

FUNCTIONAL DESCRIPTION

The XRP7674 is a synchronous, current-mode, step-down regulator with light-load efficiency. The light-load efficiency is achieved by monitoring the current through M2 and turning it off when current drops below 0A. The XRP7674 regulates input voltages from 4.5V to 18V and supplies up to 2A of load current. It uses current-mode control to regulate the output voltage. The output voltage is measured at FB through a resistive voltage divider and input to a transconductance error amplifier. The high-side switch current is compared to the output of the error amplifier to control the output voltage. The regulator utilizes internal N-channel MOSFETs to step-down the input voltage. A bootstrapping capacitor connected between BS and SW acts as a supply for high-side MOSFET. This capacitor is charged from the internal 5V supply when SW node is low. The XRP7674 has several powerful protection features including OCP, OVP, OTP, UVLO and output short-circuit.

PROGRAMMABLE SOFT-START

The soft-start time is fully programmable via CSS capacitor, placed between the SS and GND pin. The CSS is charged by a 5μA constant-current source, generating a ramp signal fed into non-inverting input of the error amplifier. This ramp regulates the voltage on comp pin during the regulator startup, thus realizing soft-start. Calculate the required CSS from:

$$CSS \approx t_{ss} \times \frac{5\mu A}{V_{FB}}$$

Where:

t_{ss} is the required soft-start time

V_{FB} is the feedback voltage (0.925V nominal)

Please note that the above is a simplified equation and will provide an approximate CSS value. For a required soft-start, a more accurate CSS can be determined based on empirical data.

OVERCURRENT PROTECTION AND HICCUP MODE

The OCP protects against accidental increase in load current or a short circuit. The current of internal switch M1 is monitored. If this current exceeds 3.5A typical then a hiccup mode is triggered. In hiccup mode, internal power FETs are turned off and the SS pin is discharged. When SS reaches 0.2V a softstart is initiated. The regulator will stay in hiccup mode until overcurrent is removed. Note that when the soft start pin is below approximately 0.5V the regulator switching frequency is 90kHz.

OVERVOLTAGE PROTECTION OVP

The XRP7674 has internal OVP. When V_{OUT} exceeds the OVP threshold (when V_{FB} exceeds 1.1V) the power switching will be turned off. The XRP7674 will restart when overvoltage condition is removed.

OVER-TEMPERATURE PROTECTION OTP

If the junction temperature exceeds 160°C the OTP circuit is triggered, turning off the internal control circuit and switched M1 and M2. When junction temperature drops below 130°C the XRP7674 will restart.

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APPLICATION INFORMATION

SETTING THE OUTPUT VOLTAGE

Use an external resistor divider to set the output voltage. Program the output voltage from:

$$R1 = R2 \times \left(\frac{V_{OUT}}{0.925V} - 1 \right)$$

Where:

R1 is the resistor between V_{OUT} and FB

R2 is the resistor between FB and GND (nominally 10k Ω)

0.925V is the nominal feedback voltage.

OUTPUT INDUCTOR

Select the output inductor for inductance L, DC current rating I_{DC} and saturation current rating I_{SAT} . I_{DC} should be larger than regulator output current. I_{SAT} , as a rule of thumb, should be 50% higher than the regulator output current. Since the regulator is rated at 2A then $I_{DC} \geq 2A$ and $I_{SAT} \geq 3A$. Calculate the inductance from:

$$L = (V_{IN} - V_{OUT}) \left(\frac{V_{OUT}}{\Delta I_L \times f_s \times V_{IN}} \right)$$

Where:

ΔI_L is peak-to-peak inductor current ripple nominally set to 30%-40% of I_{OUT}

f_s is nominal switching frequency (340kHz)

As an example, inductor values for several common output voltages are shown in tables 1 and 2.

VOUT(V)	$\Delta I_{L(p-p)}$ (A)	L(μ H)	Inductor Example
5.0	0.86	10	DR74-100-R
3.3	0.70	10	DR74-100-R
2.5	0.70	8.2	DR74-8R2-R
1.8	0.66	6.8	DR74-6R8-R
1.5	0.57	6.8	DR74-6R8-R
1.2	0.68	4.7	DR74-4R7-R

Table 1: Suggested inductor values for $V_{IN}=12V$ and $I_{OUT}=2A$

VOUT(V)	$\Delta I_{L(p-p)}$ (A)	L(μ H)	Inductor Example
3.3	0.70	4.7	DR74-4R7-R
2.5	0.78	4.7	DR74-4R7-R
1.8	0.72	4.7	DR74-4R7-R
1.5	0.66	4.7	DR74-4R7-R
1.2	0.57	4.7	DR74-4R7-R

Table 2: Suggested inductor values for $V_{IN}=5V$ and $I_{OUT}=2A$

OUTPUT CAPACITOR C_{OUT}

Select the output capacitor for voltage rating, capacitance C_{OUT} and Equivalent Series Resistance ESR. The voltage rating, as a rule of thumb, should be at least twice the output voltage. When calculating the required capacitance, usually the overriding requirement is current load-step transient. If the unloading transient (i.e., when load transitions from a high to a low current) is met, then usually the loading transient (when load transitions from a low to a high current) is met as well. Therefore calculate the C_{OUT} based on the unloading transient requirement from:

$$C_{OUT} = L \times \left(\frac{I_{High}^2 - I_{Low}^2}{(V_{OUT} + V_{transient})^2 - V_{OUT}^2} \right)$$

Where:

L is the inductance calculated in the preceding step

I_{High} is the value of load-step prior to unloading. This is nominally set equal to regulator current rating (2A).

I_{Low} is the value of load-step after unloading. This is nominally set equal to 50% of regulator current rating (1A).

$V_{transient}$ is the maximum permissible voltage transient corresponding to the load step mentioned above. $V_{transient}$ is typically specified from 3% to 5% of V_{OUT} .

ESR of the capacitor has to be selected such that the output voltage ripple requirement ΔV_{OUT} , nominally 1% of V_{OUT} , is met. Voltage ripple ΔV_{OUT} is mainly composed of two components: the resistive ripple due to ESR and capacitive ripple due to C_{OUT} charge transfer. For applications requiring low voltage ripple, ceramic capacitors are recommended

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because of their low ESR which is typically in the range of 5mΩ. Therefore ΔV_{OUT} is mainly capacitive. For ceramic capacitors calculate the ΔV_{OUT} from:

$$\Delta V_{OUT} = \frac{\Delta I_L}{8 \times C_{OUT} \times f_s}$$

Where:

ΔI_L is from table 1 or 2 in previous section

C_{OUT} is the value calculated above

f_s is nominal switching frequency (340kHz)

If tantalum or electrolytic capacitors are used then ΔV_{OUT} is essentially a function of ESR:

$$\Delta V_{OUT} = \Delta I_L \times ESR$$

INPUT CAPACITOR C_{IN}

Select the input capacitor for voltage rating, RMS current rating and capacitance. The voltage rating should be at least 50% higher than the regulator's maximum input voltage. Calculate the capacitor's current rating from:

$$I_{CIN,RMS} = I_{OUT} \times \sqrt{D \times (1 - D)}$$

Where:

I_{OUT} is regulator's maximum current (2A)

D is duty cycle ($D = V_{OUT}/V_{IN}$)

Calculate the C_{IN} capacitance from:

$$C_{IN} = \frac{I_{OUT} \times V_{OUT} \times (V_{IN} - V_{OUT})}{f_s \times V_{IN}^2 \times \Delta V_{IN}}$$

Where:

ΔV_{IN} is the permissible input voltage ripple, nominally set at 1% of V_{IN}

OPTIONAL SCHOTTKY DIODE

An optional Schottky diode may be paralleled between the GND pin and SW pin to improve the regulator efficiency. See Table 3.

Part Number	Voltage/Current Rating	Vendor
B130	30V/1A	Diodes, Inc.
SK13	30V/1A	Diodes, Inc.
MBRS130	30V/1A	International Rectifier

Table 3: Optional Schottky diode

EXTERNAL BOOTSTRAP DIODE

A low-cost diode, such as 1N4148, may provide higher efficiency when the input voltage is 5V or the output is 5V or 3.3V. Circuit configuration is shown in figures 16 and 17. The external bootstrap diode is also recommended where duty cycle (V_{OUT}/V_{IN}) is larger than 65%.

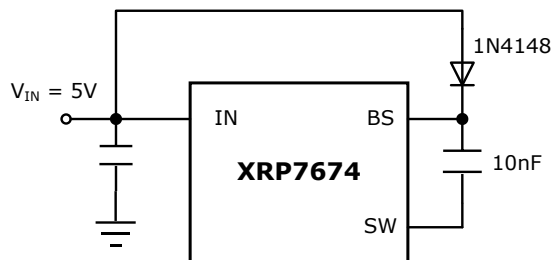


Fig. 16: Optional external bootstrap diode where input voltage is fixed 5V

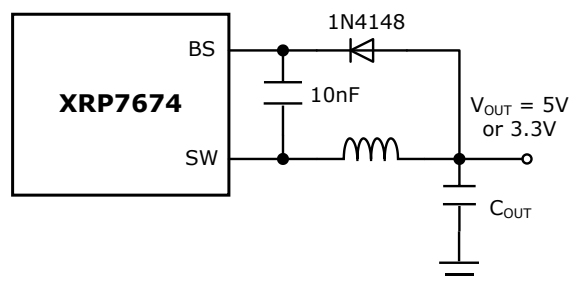


Fig. 17: Optional external bootstrap diode where output voltage is 5V or 3.3V

LOOP COMPENSATION

XRP7674 utilizes current-mode control. This allows using a minimum of external components to compensate the regulator. In general only two components are needed: RC and CC. Proper compensation of the regulator (determining RC and CC) results in optimum transient response. In terms of power supply control theory, the goals of compensation are to choose RC and CC such that the regulator loop gain has a crossover frequency f_c between 15kHz and 34kHz. The corresponding phase-margin should be between 45 degrees and 65 degrees. An important characteristic of current-mode buck regulator is its dominant pole. The frequency of the dominant pole is given by:

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$$f_p = \frac{1}{2\pi \times C_{OUT} \times R_{load}}$$

where R_{load} is the output load resistance.

The uncompensated regulator has a constant gain up to its pole frequency, beyond which the gain decreases at -20dB/decade. The zero arising from the output capacitor's ESR is inconsequential if ceramic C_{OUT} is used. This simplifies the compensation. The RC and CC, which are placed between the output of XRP7674's Error Amplifier and ground, constitute a zero. The frequency of this compensating zero is given by:

$$f_z = \frac{1}{2\pi \times RC \times CC}$$

For the typical application circuit, $RC=13k\Omega$ and $CC=4.7nF$ provide a satisfactory compensation. The XRP7674 can also be used as a pin to pin upgrade replacement for XRP7664 based designs; in this instance, the recommended RC network for XRP7664, $RC=5.6k$ and $CC=3.3nF$, can be used with satisfactory results with the XRP7674. Please contact EXAR if you need assistance with the compensation of your particular circuit.

TYPICAL APPLICATIONS

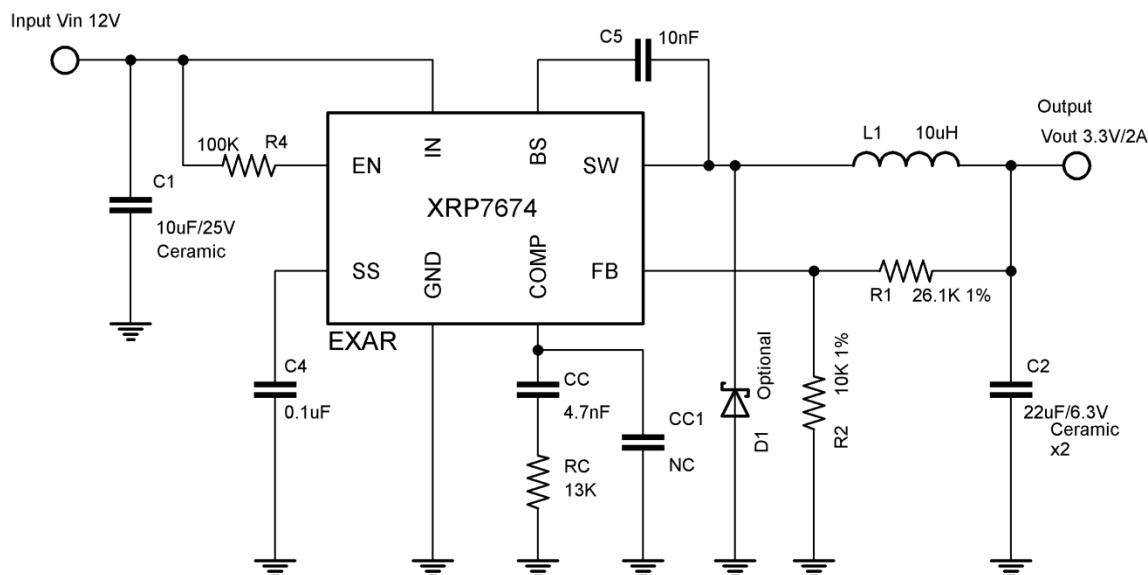


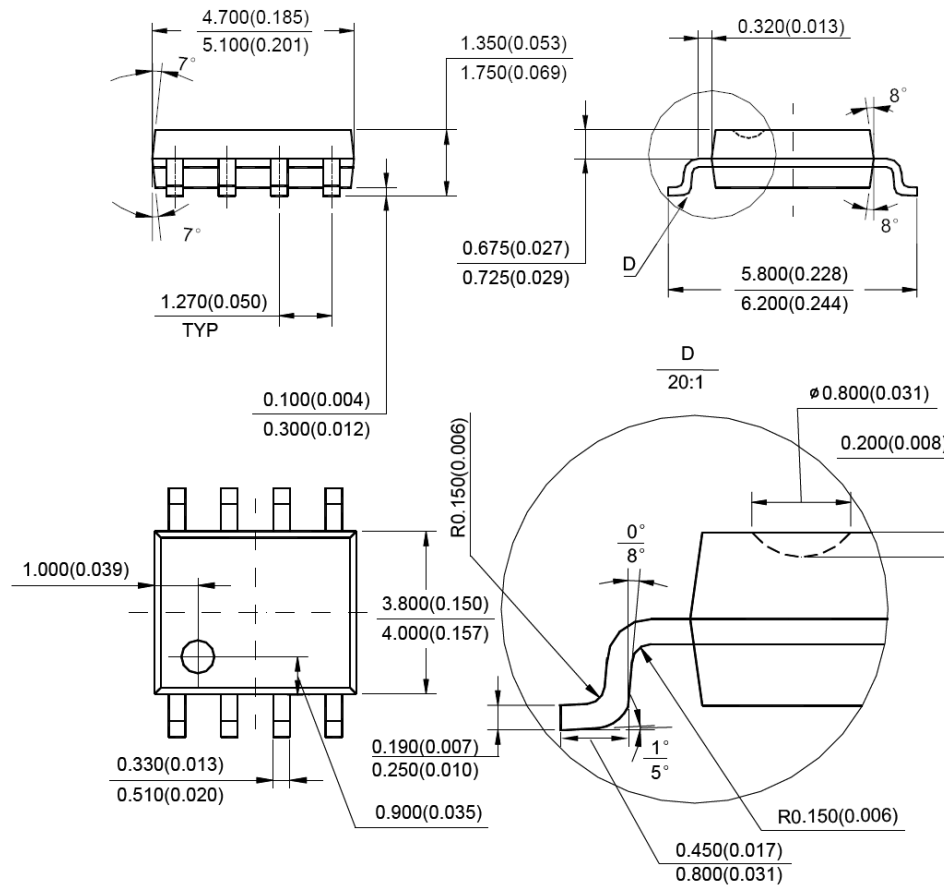
Fig. 18: XRP7674 Typical Application Diagram - 12V to 3.3V Conversion

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PACKAGE SPECIFICATION

8-Pin SOIC

Unit: mm (inch)



2A 18V Synchronous PFM/PWM Step-Down Regulator**REVISION HISTORY**

Revision	Date	Description
1.0.0	02/28/2013	Initial release of datasheet

FOR FURTHER ASSISTANCE

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