

# LTC4214-1/LTC4214-2

## ABSOLUTE MAXIMUM RATINGS

All Voltages Referred to  $V_{EE}$  (Note 1)

$V_{IN}$ .....	-0.3V to 17V
Input/Output Pins (Except SENSE and DRAIN) Voltage .....	-0.3V to 17V
SENSE Pin Voltage .....	-0.6V to 17V
Current Out of SENSE Pin (20 $\mu$ s Pulse) .....	-200mA
DRAIN Pin Minimum Voltage .....	-0.3V
Current into DRAIN Pin (100 $\mu$ s Pulse) .....	5mA
Maximum Junction Temperature .....	125°C
Operating Temperature Range	
LTC4214-1C/LTC4214-2C .....	0°C to 70°C
LTC4214-1I/LTC4214-2I .....	-40°C to 85°C
Storage Temperature Range .....	-65°C to 150°C
Lead Temperature (Soldering, 10 sec) .....	300°C

## PACKAGE/ORDER INFORMATION

	ORDER PART NUMBER
	LTC4214-1CMS LTC4214-2CMS LTC4214-1IMS LTC4214-2IMS
	MS PART MARKING
	LTABH LTABK LTABJ LTABL

Consult LTC Marketing for parts specified with wider operating temperature ranges.

## ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ .  $V_{IN} = 12\text{V}$ ,  $UV = 0\text{V} = 2.5\text{V}$  unless otherwise noted. (Note 2)

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
$V_{IN}$	Supply Voltage	●	6		16	V
$I_{IN}$	$V_{IN}$ Supply Current	$UV = 0\text{V} = 2.5\text{V}$ ●		0.8	2	mA
$V_{LKO}$	$V_{IN}$ Undervoltage Lockout	Coming Out of UVLO (Rising $V_{IN}$ ) ●		5.1	5.6	V
$V_{LKH}$	$V_{IN}$ Undervoltage Lockout Hysteresis			0.3		V
$V_{CB}$	Circuit Breaker Current Limit Voltage	$V_{CB} = (V_{SENSE} - V_{EE})$ ●	44	50	56	mV
$V_{ACL}$	Analog Current Limit Voltage	$V_{ACL} = (V_{SENSE} - V_{EE})$ , SS = Open ●	60	70	80	mV
$V_{FCL}$	Fast Current Limit Voltage	$V_{FCL} = (V_{SENSE} - V_{EE})$ ●	150	200	300	mV
$V_{SS}$	SS Voltage	After End of SS Timing Cycle		1.6		V
$R_{SS}$	SS Output Impedance			73		k $\Omega$
$I_{SS}$	SS Pin Current	$UV = 0\text{V} = 2.5\text{V}$ , $V_{SENSE} = V_{EE}$ , $V_{SS} = 0\text{V}$ (Sourcing) $UV = 0\text{V} = 0\text{V}$ , $V_{SENSE} = V_{EE}$ , $V_{SS} = 1\text{V}$ (Sinking)		-22 14		$\mu\text{A}$ mA
$V_{OS}$	Analog Current Limit Offset Voltage			10		mV
$\frac{V_{ACL} + V_{OS}}{V_{SS}}$	Ratio ( $V_{ACL} + V_{OS}$ ) to SS Voltage			0.05		V/V
$I_{GATE}$	GATE Pin Output Current	$V_{SENSE} = V_{EE}$ , $V_{GATE} = 0\text{V}$ (Sourcing) $V_{SENSE} - V_{EE} = 0.15\text{V}$ , $V_{GATE} = 3\text{V}$ (Sinking) $V_{SENSE} - V_{EE} = 0.3\text{V}$ , $V_{GATE} = 1\text{V}$ (Sinking)	●	-30 -50 17 190	-70	$\mu\text{A}$ mA mA
$V_{GATE}$	External MOSFET Gate Drive	$V_{GATE} - V_{EE}$ ●	10	11	12	V
$V_{GATEH}$	Gate High Threshold	$V_{GATEH} = V_{IN} - V_{GATE}$ for $\overline{\text{PWRGD}}$ Status		2.8		V
$V_{GATEL}$	Gate Low Threshold	(Before Gate Ramp-Up)		0.5		V
$V_{UVHI}$	UV Pin Threshold	UV Rising ●	2.137	2.25	2.363	V
$V_{UVHST}$	UV Pin Hysteresis	●	0.22	0.25	0.28	V
$V_{OVHI}$	OV Pin Threshold	OV Rising ●	2.85	3	3.15	V
$V_{OVHST}$	OV Pin Hysteresis	●	0.12	0.15	0.18	V

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**ELECTRICAL CHARACTERISTICS**

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ .  $V_{IN} = 12\text{V}$ ,  $UV = 0\text{V} = 2.5\text{V}$  unless otherwise noted. (Note 2)

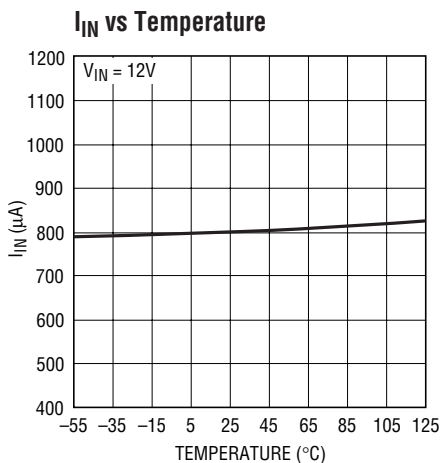
SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
I <sub>SENSE</sub>	SENSE Pin Input Current	V <sub>SENSE</sub> = 50mV	●		−15	−30	μA
I <sub>INP</sub>	UV, OV Pin Input Current	UV = OV = 2.5V	●		±0.1	±1	μA
V <sub>TMRH</sub>	TIMER Pin Voltage High Threshold				3		V
V <sub>TMRL</sub>	TIMER Pin Voltage Low Threshold				1.7		V
I <sub>TMR</sub>	TIMER Pin Current	Timer On (Initial Cycle/Latchoff/ Shutdown Cooling, Sourcing), V <sub>TMR</sub> = 2.2V			−5		μA
		Timer Off (Initial Cycle, Sinking), V <sub>TMR</sub> = 2.2V			28		mA
		Timer On (Circuit Breaker, Sourcing, I <sub>DRN</sub> = 0μA), V <sub>TMR</sub> = 2.2V			−40		μA
		Timer On (Circuit Breaker, Sourcing, I <sub>DRN</sub> = 20μA), V <sub>TMR</sub> = 2.2V			−200		μA
		Timer Off (Circuit Breaker/ Shutdown Cooling, Sinking), V <sub>TMR</sub> = 2.2V			5		μA
$\frac{\Delta I_{TMRACC}}{\Delta I_{DRN}}$	$\frac{[(I_{TMR} \text{ at } I_{DRN} = 20\mu A) - (I_{TMR} \text{ at } I_{DRN} = 0\mu A)]}{20\mu A}$	Timer On (Circuit Breaker with I <sub>DRN</sub> = 20μA)			8		μA/μA
V <sub>DRNL</sub>	DRAIN Pin Voltage Low Threshold	For $\overline{\text{PWRGD}}$ Status	●	1.109	1.232	1.355	V
I <sub>DRNL</sub>	DRAIN Leakage Current	V <sub>DRAIN</sub> = 2.5V			±0.1	±1	μA
V <sub>DRNCL</sub>	DRAIN Pin Clamp Voltage	I <sub>DRN</sub> = 20μA		3.5	4.2	5	V
V <sub>PGL</sub>	$\overline{\text{PWRGD}}$ Output Low Voltage	I <sub>PG</sub> = 1.6mA I <sub>PG</sub> = 5mA	● ●		0.2	0.4 1.1	V V
I <sub>PGH</sub>	$\overline{\text{PWRGD}}$ Pull-Up Current	V $\overline{\text{PWRGD}}$ = 0V (Sourcing)	●	−30	−50	−70	μA
t <sub>SS</sub>	SS Default Ramp Period	SS Pin Floating, V <sub>SS</sub> Ramps from 0.2V to 1.4V			130		μs
t <sub>PLLUG</sub>	UV Low to Gate Low				0.4		μs
t <sub>PHLOG</sub>	OV High to Gate Low				0.4		μs

**Note 1:** Absolute Maximum Ratings are those values beyond which the life of a device may be impaired.

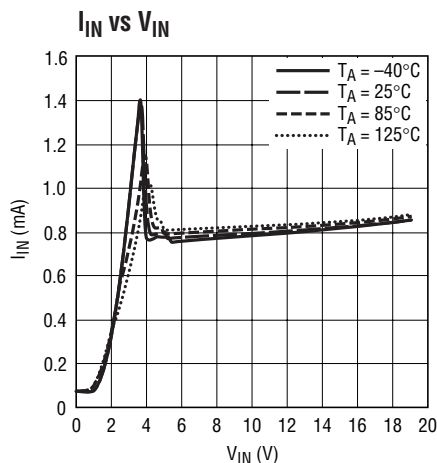
**Note 2:** All currents into device pins are positive; all currents out of device pins are negative. All voltages are referenced to  $V_{EE}$  unless otherwise specified.

**TYPICAL PERFORMANCE CHARACTERISTICS**

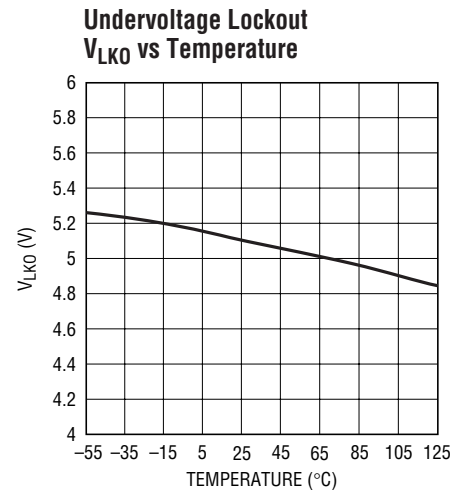
All voltages are referenced to  $V_{EE}$  Unless otherwise specified.



4214 G01



4214 G02



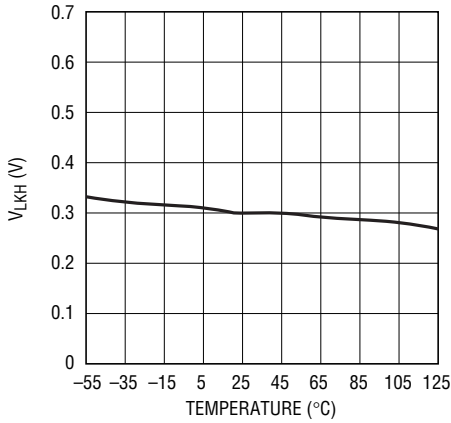
4214 G03

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## TYPICAL PERFORMANCE CHARACTERISTICS

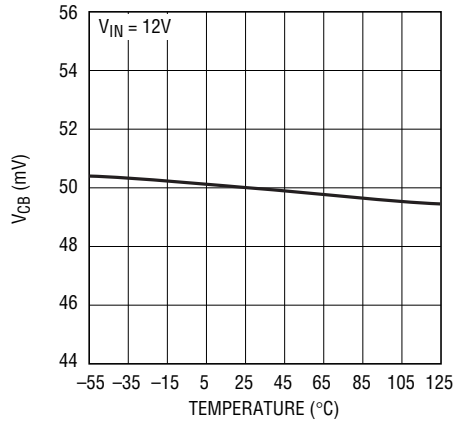
All voltages are referenced to  $V_{EE}$  Unless otherwise specified.

**Undervoltage Lockout Hysteresis  
 $V_{LKH}$  vs Temperature**



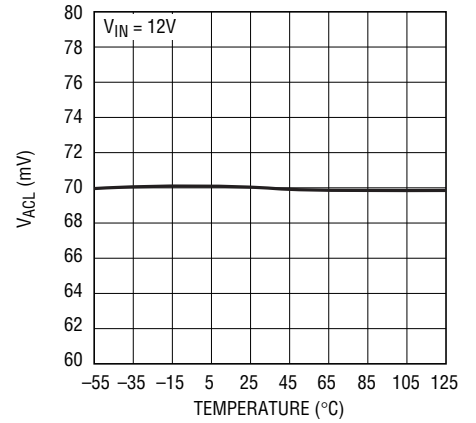
4214 G04

**Circuit Breaker Current Limit  
Voltage  $V_{CB}$  vs Temperature**



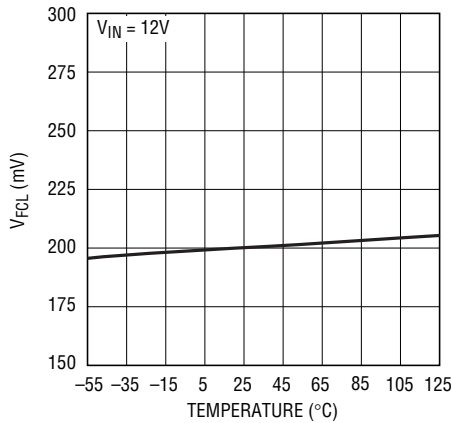
4214 G05

**Analog Current Limit Voltage  
 $V_{ACL}$  vs Temperature**



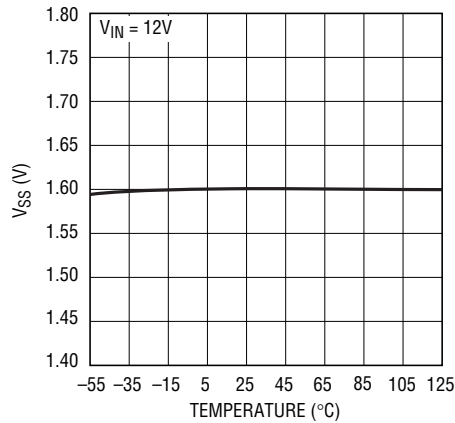
4214 G06

**Fast Current Limit Voltage  
 $V_{FCL}$  vs Temperature**



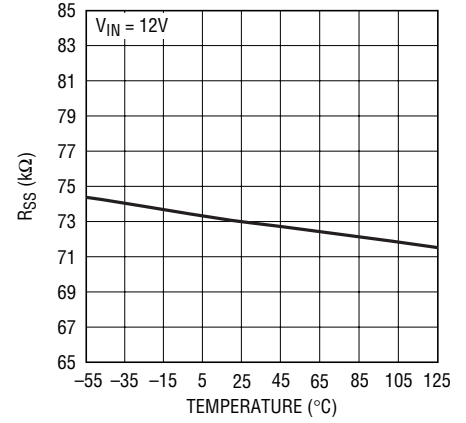
4214 G07

**$V_{SS}$  vs Temperature**



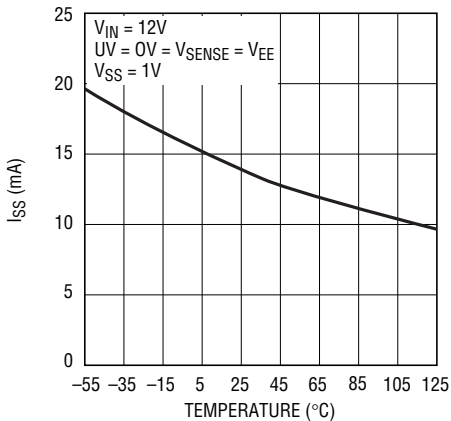
4214 G08

**$R_{SS}$  vs Temperature**



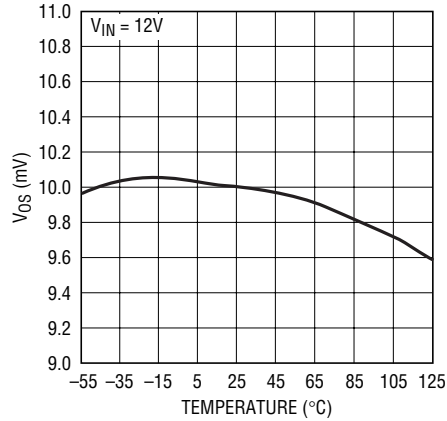
4214 G09

**$I_{SS}$  (Sinking) vs Temperature**



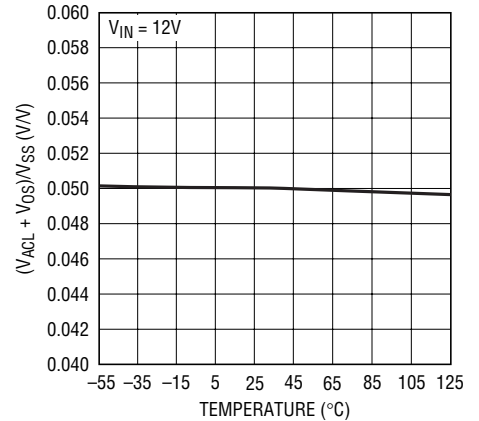
4214 G10

**$V_{OS}$  vs Temperature**



4214 G11

**$(V_{ACL} + V_{OS})/V_{SS}$  vs Temperature**



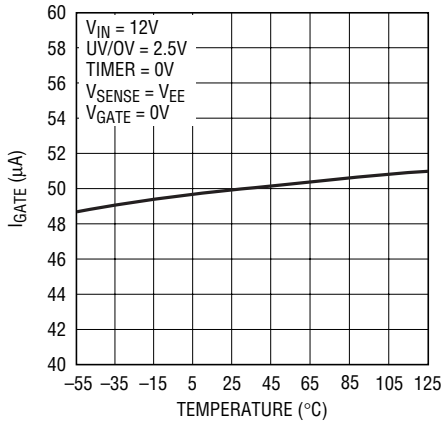
4214 G12

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# TYPICAL PERFORMANCE CHARACTERISTICS

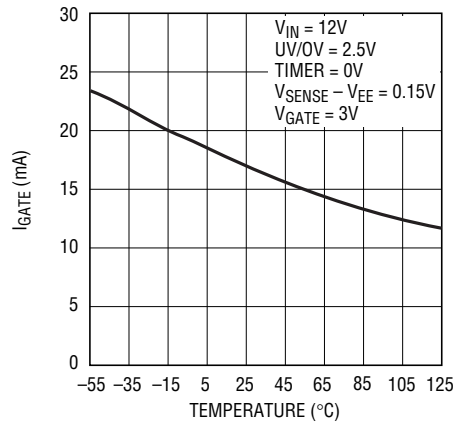
All voltages are referenced to  $V_{EE}$  Unless otherwise specified.

### $I_{GATE}$ (Sourcing) vs Temperature



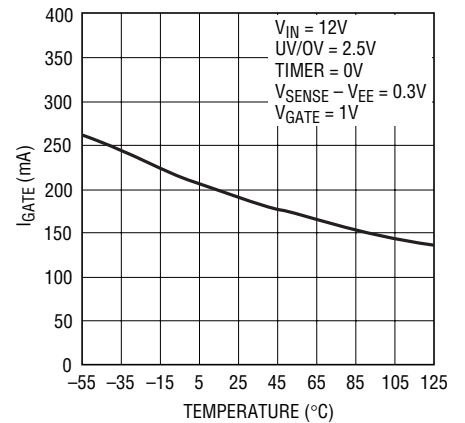
4214 G13

### $I_{GATE}$ (ACL, Sinking) vs Temperature



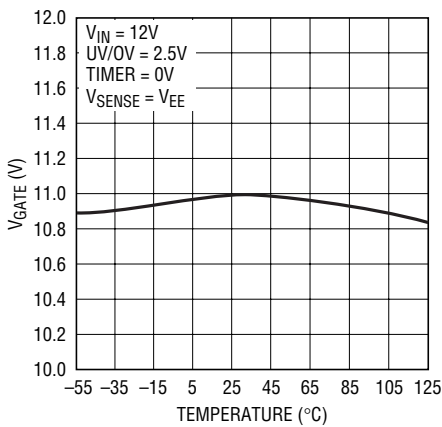
4214 G14

### $I_{GATE}$ (FCL, Sinking) vs Temperature



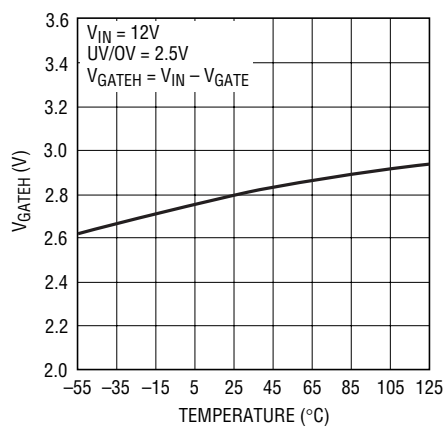
4214 G15

### $V_{GATE}$ vs Temperature



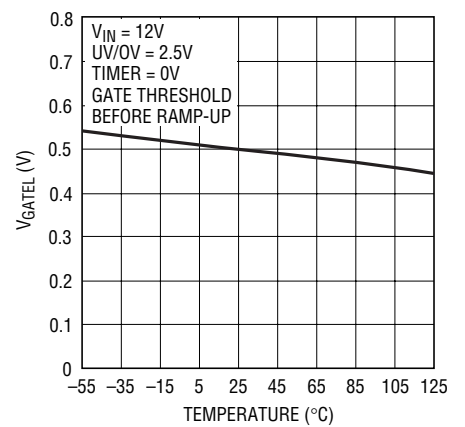
4214 G16

### $V_{GATEH}$ vs Temperature



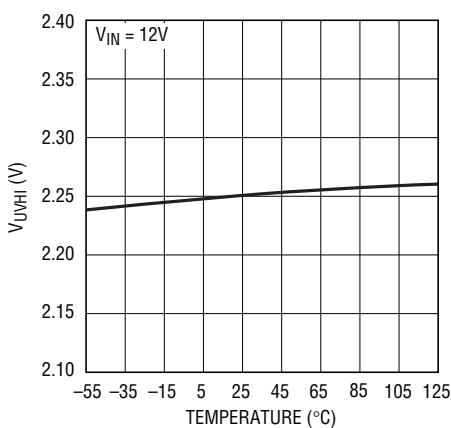
4214 G17

### $V_{GATEL}$ vs Temperature



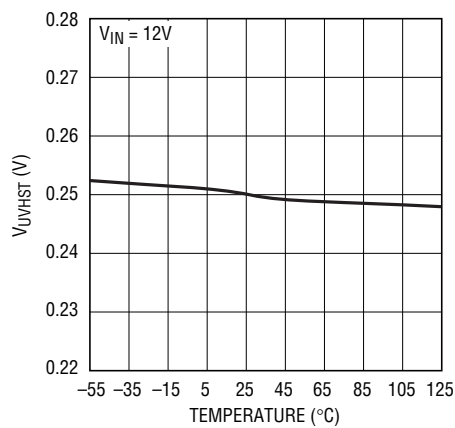
4214 G18

### $V_{UVHI}$ vs Temperature



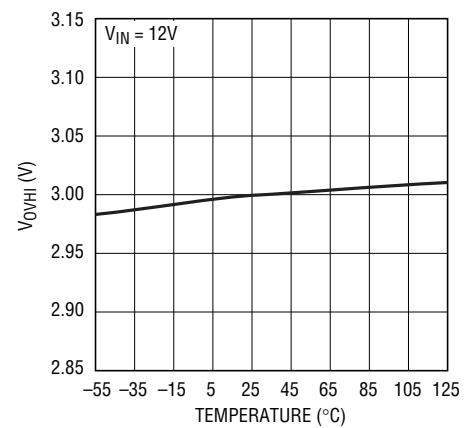
4214 G19

### $V_{UVHST}$ vs Temperature



4214 G20

### $V_{OVHI}$ vs Temperature



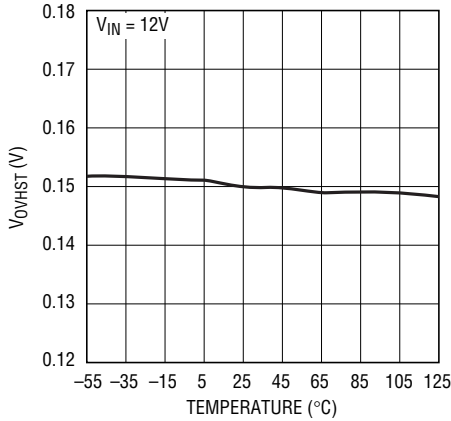
4214 G21

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## TYPICAL PERFORMANCE CHARACTERISTICS

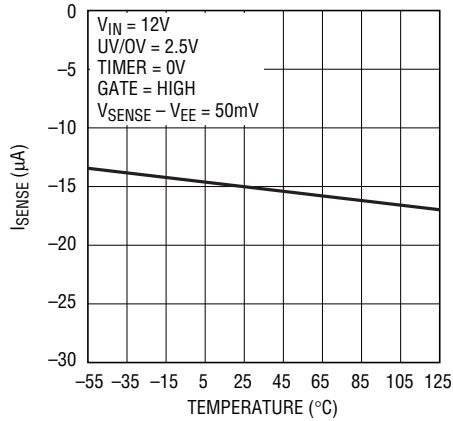
All voltages are referenced to  $V_{EE}$  Unless otherwise specified.

**V<sub>OVHST</sub> vs Temperature**



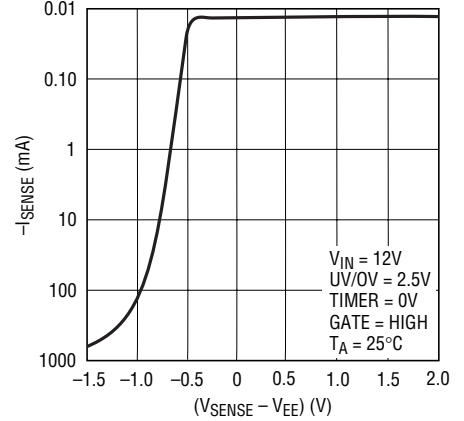
4214 G22

**I<sub>SENSE</sub> vs Temperature**



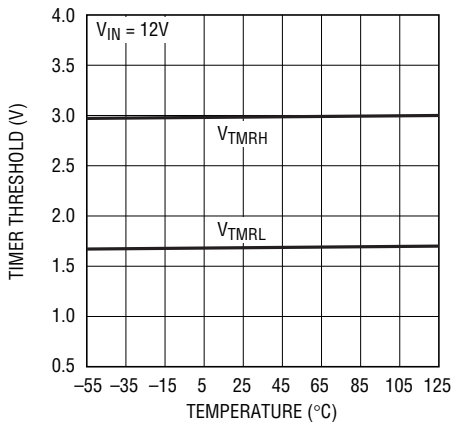
4214 G23

**I<sub>SENSE</sub> vs (V<sub>SENSE</sub> - V<sub>EE</sub>)**



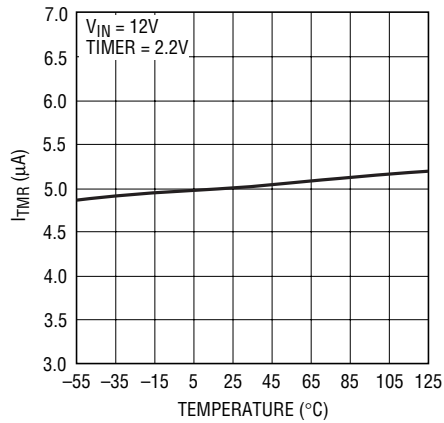
4214 G24

**TIMER Threshold vs Temperature**



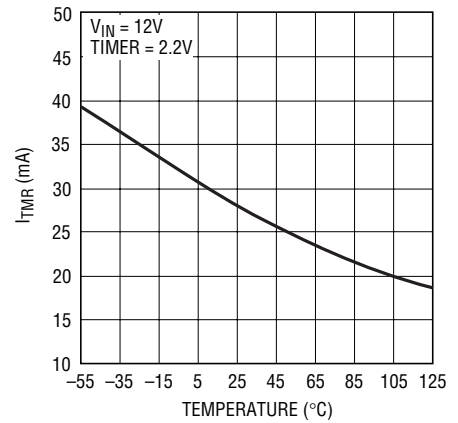
4214 G25

**I<sub>TMR</sub> (Initial Cycle, Sourcing) vs Temperature**



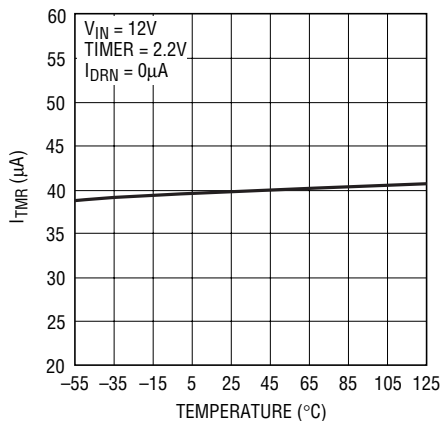
4214 G26

**I<sub>TMR</sub> (Initial Cycle, Sinking) vs Temperature**



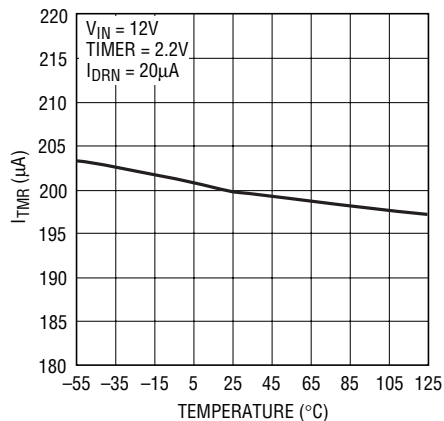
4214 G27

**I<sub>TMR</sub> (Circuit Breaker, Sourcing) vs Temperature**



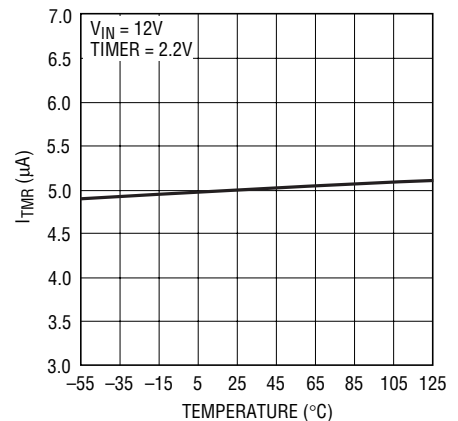
4214 G28

**I<sub>TMR</sub> (Circuit Breaker, I<sub>DRN</sub> = 20μA, Sourcing) vs Temperature**



4214 G29

**I<sub>TMR</sub> (Cooling Cycle, Sinking) vs Temperature**



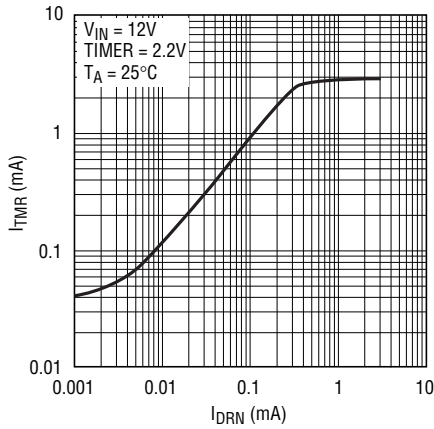
4214 G30

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# TYPICAL PERFORMANCE CHARACTERISTICS

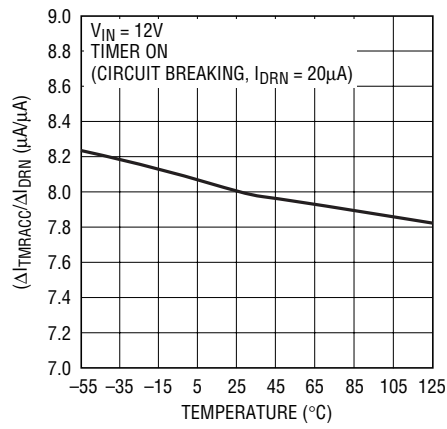
All voltages are referenced to  $V_{EE}$  Unless otherwise specified.

**$I_{TMR}$  (Circuit Breaker, Sourcing) vs  $I_{DRN}$**



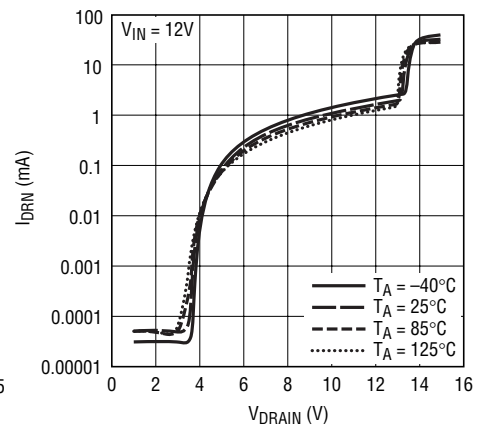
4214 G31

**$\Delta I_{TMRACC}/\Delta I_{DRN}$  vs Temperature**



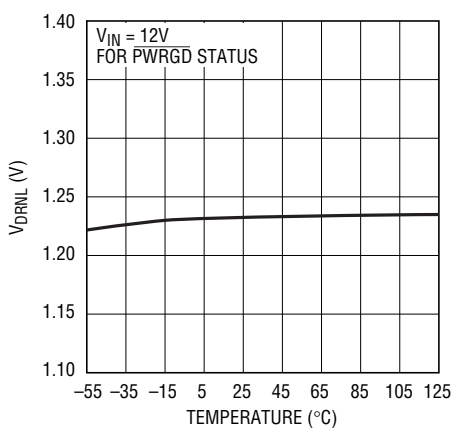
4214 G32

**$I_{DRN}$  vs  $V_{DRAIN}$**



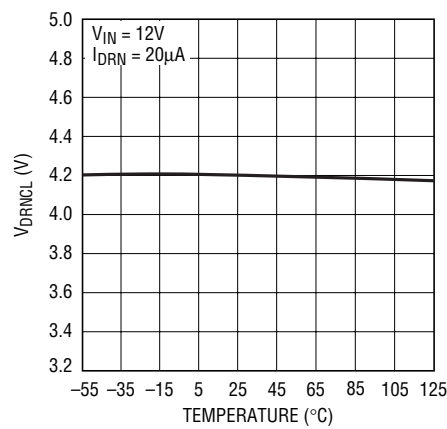
4214 G33

**$V_{DRNL}$  vs Temperature**



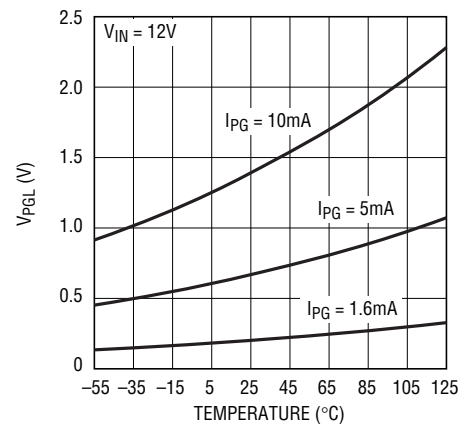
4214 G34

**$V_{DRNCL}$  vs Temperature**



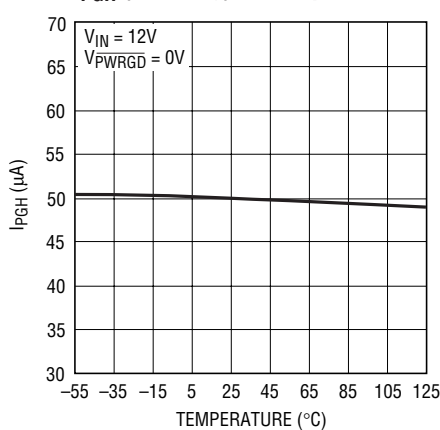
4214 G35

**$V_{PGL}$  vs Temperature**



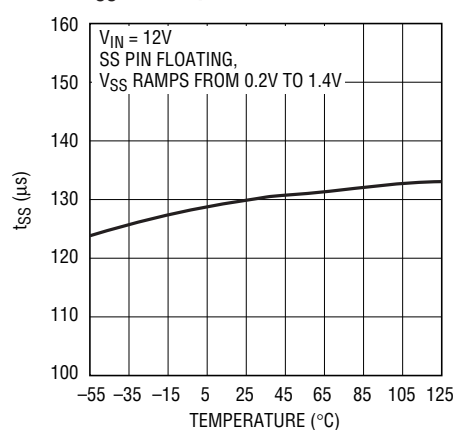
4214 G36

**$I_{PGH}$  (Sourcing) vs Temperature**



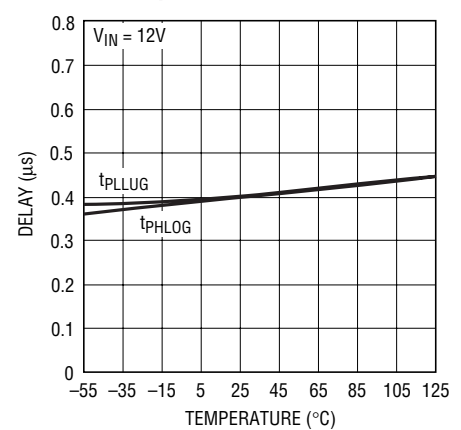
4214 G37

**$t_{SS}$  vs Temperature**



4214 G38

**$t_{PLLUG}$  and  $t_{PHLOG}$  vs Temperature**



4214 G39

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## PIN FUNCTIONS

**V<sub>IN</sub> (Pin 1):** Positive Supply Input. Connect this pin to the positive side of the supply via a resistor. An internal undervoltage lockout (UVLO) circuit holds GATE low until the V<sub>IN</sub> pin is greater than V<sub>LKO</sub> (5.1V), overriding UV and OV. If UV is high, OV is low and V<sub>IN</sub> comes out of UVLO, TIMER starts an initial timing cycle before initiating a GATE ramp-up. If V<sub>IN</sub> drops below approximately 4.8V, GATE pulls low immediately.

**PWRGD (Pin 2):** Power Good Status Output. At start-up, PWRGD latches low if DRAIN is below 1.232V and GATE is within 2.8V of V<sub>IN</sub>. PWRGD status is reset by UV, V<sub>IN</sub> (UVLO) or a circuit breaker fault timeout. This pin is internally pulled high by a 50μA current source.

**SS (Pin 3):** Soft-Start Pin. This pin is used to ramp inrush current during start up, thereby effecting control over di/dt. A 20x attenuated version of the SS pin voltage is presented to the current limit amplifier. This attenuated voltage limits the MOSFET's drain current through the sense resistor during the soft-start current limiting. At the beginning of a start-up cycle, the SS capacitor (C<sub>SS</sub>) is ramped by a 22μA current source. The GATE pin is held low until SS exceeds  $20 \cdot V_{OS} = 0.2V$ . SS is internally shunted by a 73k resistor (R<sub>SS</sub>) which limits the SS pin voltage to 1.6V. This corresponds to an analog current limit SENSE voltage of 70mV. If the SS capacitor is omitted, the SS pin ramps from 0V to 1.6V in about 220μs. The SS pin is pulled low under any of the following conditions: in UVLO, in an undervoltage condition, in an overvoltage condition, during the initial timing cycle or when the circuit breaker fault times out.

**SENSE (Pin 4):** Circuit Breaker/Current Limit Sense Pin. Load current is monitored by a sense resistor R<sub>S</sub> connected between SENSE and V<sub>EE</sub>, and controlled in three steps. If SENSE exceeds V<sub>CB</sub> (50mV), the circuit breaker comparator activates a  $(40\mu A + 8 \cdot I_{DRN})$  TIMER pull-up current. If SENSE exceeds V<sub>ACL</sub> (70mV), the analog current limit amplifier pulls GATE down to regulate the MOSFET current at V<sub>ACL</sub>/R<sub>S</sub>. In the event of a catastrophic short-circuit, SENSE may overshoot 70mV. If SENSE reaches

V<sub>FCL</sub> (200mV), the fast current limit comparator pulls GATE low with a strong pull-down. To disable the circuit breaker and current limit functions, connect SENSE to V<sub>EE</sub>.

**V<sub>EE</sub> (Pin 5):** Negative Supply Voltage Input. Connect this pin to the negative side of the power supply.

**GATE (Pin 6):** N-Channel MOSFET Gate Drive Output. This pin is pulled high by a 50μA current source. GATE is pulled low by invalid conditions at V<sub>IN</sub> (UVLO), UV, OV, or a circuit breaker fault timeout. GATE is actively servoed to control the fault current as measured at SENSE. A compensation capacitor at GATE stabilizes this loop. A comparator monitors GATE to ensure that it is low before allowing an initial timing cycle, GATE ramp-up after an overvoltage event or restart after a current limit fault. During GATE start-up, a second comparator detects if GATE is within 2.8V of V<sub>IN</sub> before PWRGD is set.

**DRAIN (Pin 7):** Drain Sense Input. DRAIN measures the drain-source voltage of the external N-channel MOSFET switch for two purposes: first, a comparator detects when V<sub>DS</sub> < 1.232V and together with the GATE high comparator, controls the status of the PWRGD output. Second, if V<sub>DS</sub> is greater than the DRAIN clamp of approximately 4.2V (V<sub>DRNCL</sub>), the current through resistor R<sub>D</sub> is multiplied by 8 and added to the TIMER's 40μA pull-up current during a circuit breaker fault cycle. This reduces the fault time and MOSFET heating under conditions of high dissipation.

**OV (Pin 8):** Overvoltage Input. The active high threshold at the OV pin is set at 3V with respect to V<sub>EE</sub> and exhibits 0.15V hysteresis. If OV > 3V, GATE pulls low. When OV returns below 2.85V, GATE start-up begins without an initial timing cycle. If an overvoltage condition occurs in the middle of an initial timing cycle, the initial timing cycle is restarted after the overvoltage condition goes away. An overvoltage condition does not reset the PWRGD flag. The internal UVLO at V<sub>IN</sub> always overrides OV. A 1nF to 10nF capacitor at OV prevents transients and switching noise from affecting the OV thresholds and prevents glitches at the GATE pin.

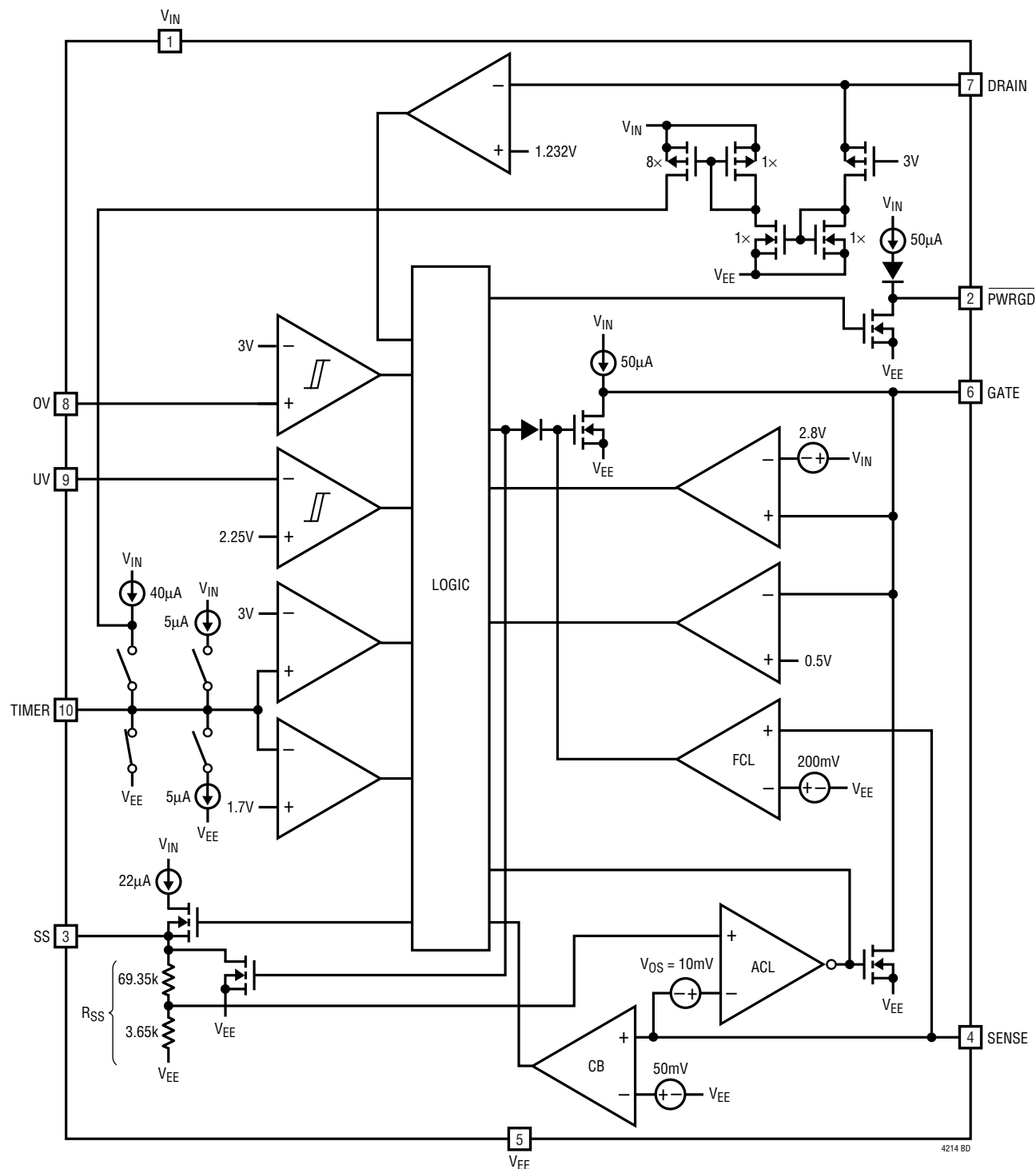
## PIN FUNCTIONS

**UV (Pin 9):** Undervoltage Input. The active high threshold at the UV pin is set at 2.25V with respect to  $V_{EE}$  and exhibits 0.25V hysteresis. If  $UV < 2V$ ,  $\overline{PWRGD}$  pulls high, both GATE and TIMER pull low. If UV rises above 2.25V, this initiates an initial timing cycle followed by GATE start-up. The internal UVLO at  $V_{IN}$  always overrides UV. A low at UV resets an internal fault latch. A 1nF to 10nF capacitor at UV prevents transients and switching noise from affecting the UV thresholds and prevents glitches at the GATE pin.

**TIMER (Pin 10):** Timer Input. TIMER is used to generate an initial timing delay at start-up and to delay shutdown in the event of an output overload (circuit breaker fault). TIMER starts an initial timing cycle when the following conditions are met: UV is high, OV is low,  $V_{IN}$  clears UVLO, TIMER pin is low, GATE is lower than  $V_{GATEL}$ ,  $SS < 0.2V$ , and  $V_{SENSE} - V_{EE} < V_{CB}$ . A pull-up current of 5 $\mu$ A then charges  $C_T$ , generating a time delay. If  $C_T$  charges to  $V_{TMRH}$  (3V), the timing cycle terminates, TIMER quickly pulls low and GATE is activated.

If SENSE exceeds 50mV while GATE is high, a circuit breaker cycle begins with a 40 $\mu$ A pull-up current charging  $C_T$ . If DRAIN is approximately 4.2V during this cycle, the timer pull-up has an additional current of  $8 \cdot I_{DRN}$ . If SENSE drops below 50mV before TIMER reaches 3V, a 5 $\mu$ A pull-down current slowly discharges the  $C_T$ . In the event that  $C_T$  eventually integrates up to the  $V_{TMRH}$  threshold, the circuit breaker trips, GATE quickly pulls low and  $\overline{PWRGD}$  pulls high. The LTC4214-1 TIMER pin latches high with a 5 $\mu$ A pull-up source. This latched fault is cleared by either pulling TIMER low with an external device or by pulling UV below 2V. The LTC4214-2 starts a shutdown cooling cycle following an overcurrent fault. This cycle consists of 4 discharging ramps and 3 charging ramps. The charging and discharging currents are 5 $\mu$ A and TIMER ramps between its 1.7V and 3V thresholds. At the completion of a shutdown cooling cycle, the LTC4214-2 attempts a start-up cycle.

BLOCK DIAGRAM



4214 BD



## OPERATION

turn on gradually so that the inrush into the load capacitance remains a low value. The output will simply ramp to  $-12\text{V}$  and the LTC4214 will fully enhance the MOSFET. A second possibility is that the load current exceeds the soft-start current limit threshold of  $[V_{SS}(t)/20 - V_{OS}]/R_S$ . In this case the LTC4214 will ramp the output by sourcing soft-start limited current into the load capacitance. If the soft-start voltage is below  $1.2\text{V}$ , the circuit breaker TIMER is held low. Above  $1.2\text{V}$ , TIMER ramps up. It is important to set the timer delay so that, regardless of which start-up mode is used, the TIMER ramp is less than one circuit breaker delay time. If this condition is not met, the LTC4214-1 may shut down after one circuit breaker delay time whereas the LTC4214-2 may continue to autoretry.

### Board Removal

If the board is withdrawn from the card cage, the UV/OV divider is the first to lose connection. This shuts off the MOSFET and commutates the flow of current in the connector. When the power pins subsequently separate, there is no arcing.

### Current Control

Three levels of protection handle short-circuit and overload conditions. Load current is monitored by SENSE and resistor  $R_S$ . There are three distinct thresholds at SENSE:  $50\text{mV}$  for a timed circuit breaker function;  $70\text{mV}$  for an analog current limit loop; and  $200\text{mV}$  for a fast, feedforward comparator which limits peak current in the event of a catastrophic short-circuit.

If, owing to an output overload, the voltage drop across  $R_S$  exceeds  $50\text{mV}$ , TIMER sources  $40\mu\text{A}$  into  $C_T$ .  $C_T$  eventually charges to a  $3\text{V}$  threshold and the LTC4214 shuts off. If the overload goes away before  $C_T$  reaches  $3\text{V}$  and SENSE measures less than  $50\text{mV}$ ,  $C_T$  slowly discharges ( $5\mu\text{A}$ ). In this way the LTC4214's circuit breaker function responds to low duty cycle overloads and accounts for fast heating and slow cooling characteristics of the MOSFET.

Higher overloads are handled by an analog current limit loop. If the drop across  $R_S$  reaches  $70\text{mV}$ , the current limiting loop servos the MOSFET gate and maintains a constant output current of  $70\text{mV}/R_S$ . In current limit mode,  $V_{OUT}$  typically rises and this increases MOSFET heating. If  $V_{OUT} > V_{DRNCL}$  ( $4.2\text{V}$ ), connecting an external resistor,  $R_D$ , between  $V_{OUT}$  and DRAIN allows the fault timing cycle to be shortened by accelerating the charging of the TIMER capacitor. The TIMER pull-up current is increased by  $8 \cdot I_{DRN}$ . Note that because  $SENSE > 50\text{mV}$ , TIMER charges  $C_T$  during this time and the LTC4214 will eventually shut down.

Low impedance failures on the load side of the LTC4214 can produce high current slew rates. Under these conditions, overshoot is inevitable. A fast SENSE comparator with a threshold of  $200\text{mV}$  detects overshoot and pulls GATE low much harder and hence much faster than the weaker current limit loop. The  $70\text{mV}/R_S$  current limit loop then takes over and servos the current as previously described. As before, TIMER runs and shuts down the LTC4214 when  $C_T$  reaches  $3\text{V}$ .

If  $C_T$  reaches  $3\text{V}$ , the LTC4214-1 latches off with a  $5\mu\text{A}$  pull-up current source whereas the LTC4214-2 starts a shutdown cooling cycle. The LTC4214-1 circuit breaker latch is reset by either pulling UV momentarily low or dropping the input voltage  $V_{IN}$  below the internal UVLO threshold of  $4.8\text{V}$  or pulling TIMER momentarily low with a switch. The LTC4214-2 retries after its shutdown cooling cycle.

Although short-circuits are the most obvious fault type, several operating conditions may invoke overcurrent protection. Noise spikes from the backplane or load, transient currents caused by faults on adjacent circuit boards sharing the same power bus or the insertion of non-hot-swappable products could cause higher than anticipated input current and temporary detection of an overcurrent condition. The action of TIMER and  $C_T$  rejects these events allowing the LTC4214 to "ride out" temporary overloads and disturbances that could trip a simple current comparator and, in some cases, blow a fuse.

## APPLICATIONS INFORMATION

### SUPPLY VOLTAGE

The LTC4214 requires a ( $V_{IN} - V_{EE}$ ) voltage of 6V to 16V to function. This can be derived from GND and  $-12V$  of a  $-12V$  system or the 3.3V and  $-5.2V$  of a  $-5.2V$  system. The positive supply is connected to  $V_{IN}$  via an RC network so that the LTC4214 can have a usable  $V_{IN}$  during load short or other transient events when ( $V_{IN} - V_{EE}$ ) glitches below 6V.

### INTERNAL UNDERVOLTAGE LOCKOUT (UVLO)

A hysteretic comparator, UVLO, monitors  $V_{IN}$  for undervoltage. The thresholds are defined by  $V_{LKO}$  and its hysteresis,  $V_{LKH}$ . When  $V_{IN}$  rises above 5.1V ( $V_{LKO}$ ) the chip is enabled; below 4.8V ( $V_{LKO} - V_{LKH}$ ) it is disabled and GATE is pulled low. The UVLO function at  $V_{IN}$  should not be confused with the UV/OV pins. These are completely separate functions.

### UV/OV COMPARATORS

An UV hysteretic comparator detects undervoltage conditions at the UV pin, with the following thresholds:

$$UV \text{ low-to-high } (V_{UVHI}) = 2.25V$$

$$UV \text{ high-to-low } (V_{UVHI} - V_{UVHST}) = 2V$$

An OV hysteretic comparator detects overvoltage conditions at the OV pin, with the following thresholds:

$$OV \text{ low-to-high } (V_{OVHI}) = 3V$$

$$OV \text{ high-to-low } (V_{OVHI} - V_{OVHST}) = 2.85V$$

In Figure 2, a divider ( $R1$ - $R2$ ) is used to scale the supply voltage of  $12V \pm 10\%$ . Using  $R1 = 121k$  and  $R2 = 32.4k$  gives a typical operating range of 10.7V to 13.5V. The under and overvoltage shutdown thresholds are then 9.5V to 14.2V. 1% divider resistors are recommended to preserve threshold accuracy.

The  $R1$ - $R2$  divider values shown in Figure 2 set a standing current of slightly more than  $75\mu A$  and define an impedance at UV/OV of  $25k\Omega$ . In most applications,  $25k\Omega$  impedance coupled with 250mV UV hysteresis makes the LTC4214 insensitive to noise. If more noise immunity is desired, add a 1nF to 10nF filter capacitor from UV/OV to  $V_{EE}$ .

Separate UV and OV pins can be used for a wider operating range such as 10V to 14V as shown in Figure 3. Other combinations are possible with different resistor arrangements.

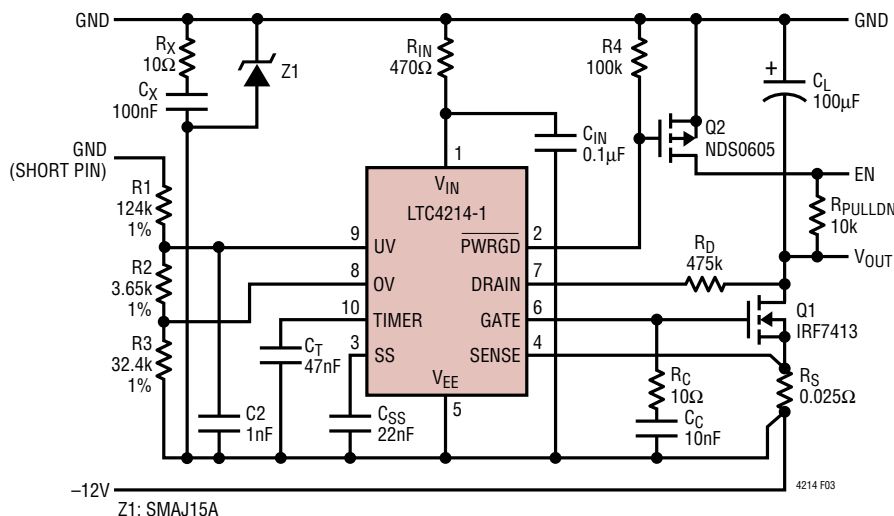


Figure 3.  $-12V/2A$  Application with Wider Input Operating Range

## APPLICATIONS INFORMATION

### UV/OV OPERATION

A low input to the UV comparator will reset the LTC4214 and pull the GATE and TIMER pins low. A low-to-high UV transition will initiate an initial timing sequence if the other interlock conditions are met. A high-to-low transition in the UV comparator immediately shuts down the LTC4214, pulls the MOSFET gate low and resets the latched PWRGD high.

Overvoltage conditions detected by the OV comparator will also pull GATE low, thereby shutting down the load. However, it will not reset the circuit breaker TIMER, PWRGD flag or shutdown cooling timer. Returning the supply voltage to an acceptable range restarts the GATE pin if all the interlock conditions except TIMER are met. Only during the initial timing cycle does an OV condition reset the TIMER.

### DRAIN

Connecting an external resistor,  $R_D$ , to the dual function DRAIN pin allows  $V_{OUT}$  sensing without it being damaged by large voltage transients. Below 3V, negligible pin leakage allows a DRAIN low comparator to detect  $V_{OUT}$  less than 1.232V ( $V_{DRNL}$ ). This condition, together with the GATE low comparator, sets the PWRGD flag.

If  $V_{OUT} > V_{DRNCL}$  (4.2V), the DRAIN pin is clamped at about 4.2V and the current flowing in  $R_D$  is given by:

$$I_{DRN} \approx \frac{V_{OUT} - V_{DRNCL}}{R_D} \quad (1)$$

This current is scaled up 8 times during a circuit breaker fault and is added to the nominal 40μA TIMER current. This accelerates the fault TIMER pull-up when the MOSFET's drain-source voltage exceeds 4.2V and effectively shortens the MOSFET heating duration.

### TIMER

The operation of the TIMER pin is somewhat complex as it handles several key functions. A capacitor  $C_T$  is used at TIMER to provide timing for the LTC4214. Four different charging and discharging modes are available at TIMER:

- 1) A 5μA slow charge; initial timing and shutdown cooling delay.
- 2) A  $(40\mu A + 8 \cdot I_{DRN})$  fast charge; circuit breaker delay.
- 3) A 5μA slow discharge; circuit breaker "cool off" and shutdown cooling.
- 4) Low impedance switch; resets the TIMER capacitor after an initial timing delay, in UVLO, in UV and in OV during initial timing.

For initial start-up, the 5μA pull-up is used. The low impedance switch is turned off and the 5μA current source is enabled when the interlock conditions are met.  $C_T$  charges to 3V in a time period given by:

$$t = \frac{3V \cdot C_T}{5\mu A} \quad (2)$$

When  $C_T$  reaches 3V ( $V_{TMRH}$ ), the low impedance switch turns on and discharges  $C_T$ . A GATE start-up cycle begins and both SS and GATE are released.

### CIRCUIT BREAKER TIMER OPERATION

If the SENSE pin detects more than a 50mV drop across  $R_S$ , the TIMER pin charges  $C_T$  with  $(40\mu A + 8 \cdot I_{DRN})$ . If  $C_T$  charges to 3V, the GATE pin pulls low and the LTC4214-1 latches off while the LTC4214-2 starts a shutdown cooling cycle. The LTC4214-1 remains latched off until the UV pin is momentarily pulsed low or TIMER is momentarily discharged low by an external switch or  $V_{IN}$  dips below UVLO and is then restored. The circuit breaker timeout period is given by:

$$t = \frac{3V \cdot C_T}{40\mu A + 8 \cdot I_{DRN}} \quad (3)$$

If  $V_{OUT} < 3V$ , an internal PMOS device isolates any DRAIN pin leakage current, making  $I_{DRN} = 0\mu A$  in Equation (3). If  $V_{OUT} > 4.2V$  ( $V_{DRNCL}$ ) during the circuit breaker fault period, the charging of  $C_T$  accelerates by  $8 \cdot I_{DRN}$  of Equation (1).

Intermittent overloads may exceed the 50mV threshold at SENSE, but, if their duration is sufficiently short, TIMER will not reach 3V and the LTC4214 will not shut the external

## APPLICATIONS INFORMATION

MOSFET off. To handle this situation, the TIMER discharges  $C_T$  slowly with a  $5\mu\text{A}$  pull-down whenever the SENSE voltage is less than  $50\text{mV}$ . Therefore, any intermittent overload with  $V_{\text{OUT}} < 3\text{V}$  and an aggregate duty cycle of 12.5% or more will eventually trip the circuit breaker and shut down the LTC4214. Figure 4 shows the circuit breaker response time in seconds normalized to  $1\mu\text{F}$  for  $I_{\text{DRN}} = 0\mu\text{A}$ . The asymmetric charging and discharging of  $C_T$  is a fair gauge of MOSFET heating.

The normalized circuit response time is estimated by

$$\frac{t}{C_T(\mu\text{F})} = \frac{3}{[(40 + 8 \cdot I_{\text{DRN}}) \cdot D - 5]} \quad (4)$$

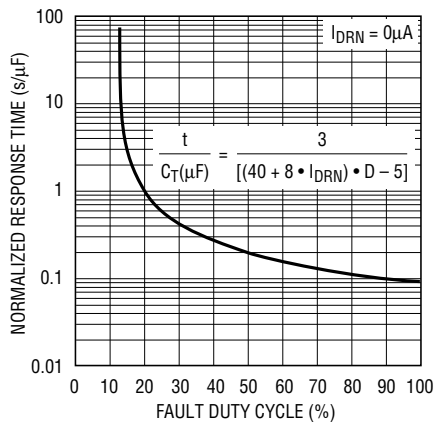


Figure 4. Circuit-Breaker Response Time

### SHUTDOWN COOLING CYCLE

For the LTC4214-1 (latchoff version), TIMER latches high with a  $5\mu\text{A}$  pull-up after the circuit breaker fault TIMER reaches  $3\text{V}$ . For the LTC4214-2 (automatic retry version), a shutdown cooling cycle begins if TIMER reaches the  $3\text{V}$  threshold. TIMER starts with a  $5\mu\text{A}$  pull-down until it reaches the  $1.7\text{V}$  threshold. Then, the  $5\mu\text{A}$  pull-up turns back on until TIMER reaches the  $3\text{V}$  threshold. Four  $5\mu\text{A}$

pull-down cycles and three  $5\mu\text{A}$  pull-up cycles occur between the  $1.7\text{V}$  and  $3\text{V}$  thresholds, creating a time interval given by:

$$t_{\text{SHUTDOWN}} = \frac{7 \cdot 1.3\text{V} \cdot C_T}{5\mu\text{A}} \quad (5)$$

At the  $1.7\text{V}$  threshold of the last pull-down cycle, a GATE ramp-up is attempted.

### SOFT-START

Soft-start limits the inrush current profile during GATE start-up. Unduly long soft-start intervals can exceed the MOSFET's SOA rating if powering up into an active load. If SS floats, an internal current source ramps SS from  $0\text{V}$  to  $1.6\text{V}$  in about  $220\mu\text{s}$ . Connecting an external capacitor  $C_{\text{SS}}$  from SS to ground modifies the ramp to approximate an RC response of:

$$V_{\text{SS}}(t) \approx V_{\text{SS}} \cdot \left( 1 - e^{-\frac{t}{R_{\text{SS}} \cdot C_{\text{SS}}}} \right) \quad (6)$$

An internal resistor divider ( $69.35\text{k}/3.65\text{k}$ ) scales  $V_{\text{SS}}(t)$  down by 20 times to give the analog current limit threshold:

$$V_{\text{ACL}}(t) = \frac{V_{\text{SS}}(t)}{20} - V_{\text{OS}} \quad (7)$$

This allows the inrush current to be limited to  $V_{\text{ACL}}(t)/R_{\text{S}}$ . The offset voltage,  $V_{\text{OS}}$  ( $10\text{mV}$ ), ensures  $C_{\text{SS}}$  is sufficiently discharged and the ACL amplifier is in current limit before GATE start-up. SS is pulled low under any of the following conditions: in UVLO, in an undervoltage condition, in an overvoltage condition, during the initial timing cycle or when the circuit breaker fault times out.

## APPLICATIONS INFORMATION

### GATE

GATE is pulled low to  $V_{EE}$  under any of the following conditions: in UVLO, in an undervoltage condition, in an overvoltage condition, during the initial timing cycle or when the circuit breaker fault times out. When GATE turns on, a  $50\mu\text{A}$  current source charges the MOSFET gate and any associated external capacitance. The gate drive is limited to no more than  $V_{IN}$ .

Gate-drain capacitance ( $C_{GD}$ ) feedthrough at the first abrupt application of power can cause a gate-source voltage sufficient to turn on the MOSFET. A unique circuit pulls GATE low with practically no usable voltage at  $V_{IN}$  and eliminates current spikes at insertion. A large external gate-source capacitor is thus unnecessary for the purpose of compensating  $C_{GD}$ . Instead, a smaller value ( $\geq 5\text{nF}$ ) capacitor  $C_C$  is adequate.  $C_C$  also provides compensation for the analog current limit loop.

GATE has two comparators: the GATE low comparator looks for  $< 0.5\text{V}$  threshold prior to initial timing or a GATE start-up cycle; the GATE high comparator looks for  $< 2.8\text{V}$  relative to  $V_{IN}$  and, together with the DRAIN low comparator, sets PWRGD status during GATE start-up.

### SENSE

The SENSE pin is monitored by the circuit breaker (CB) comparator, the analog current limit (ACL) amplifier and the fast current limit (FCL) comparator. Each of these three measures the potential of SENSE relative to  $V_{EE}$ . When SENSE exceeds  $50\text{mV}$ , the CB comparator activates the  $40\mu\text{A}$  TIMER pull-up. At  $70\text{mV}$ , the ACL amplifier serves the MOSFET current and, at  $200\text{mV}$ , the FCL comparator abruptly pulls GATE low in an attempt to bring the MOSFET current under control. If any of these conditions persists long enough for TIMER to charge  $C_T$  to  $3\text{V}$  (see Equation 3), the LTC4214 shuts down and pulls GATE low.

If the SENSE pin encounters a voltage greater than  $70\text{mV}$ , the ACL amplifier will servo GATE downwards in an attempt to control the MOSFET current. Since GATE

overdrives the MOSFET in normal operation, the ACL amplifier needs time to discharge GATE to the threshold of the MOSFET. For a mild overload the ACL amplifier can control the MOSFET current, but in the event of a severe overload the current may overshoot. At  $\text{SENSE} = 200\text{mV}$  the FCL comparator takes over, quickly discharging the GATE pin to near  $V_{EE}$  potential. FCL then releases and the ACL amplifier takes over. All the while TIMER is running. The effect of FCL is to add a nonlinear response to the control loop in favor of reducing MOSFET current.

Owing to inductive effects in the system, FCL typically overcorrects the current limit loop and GATE undershoots. A zero in the loop (resistor  $R_C$  in series with the gate capacitor) helps the ACL amplifier to recover.

### SHORT-CIRCUIT OPERATION

Circuit behavior arising from a load side low impedance short is shown in Figure 5 for the LTC4214. Initially, the current overshoots the fast current limit level of  $V_{\text{SENSE}} = 200\text{mV}$  (Trace 2) as the GATE pin works to bring  $V_{GS}$  under control (Trace 3). The overshoot glitches the backplane in the negative direction and when the current is reduced to  $70\text{mV}/R_S$ , the backplane responds by glitching in the positive direction.

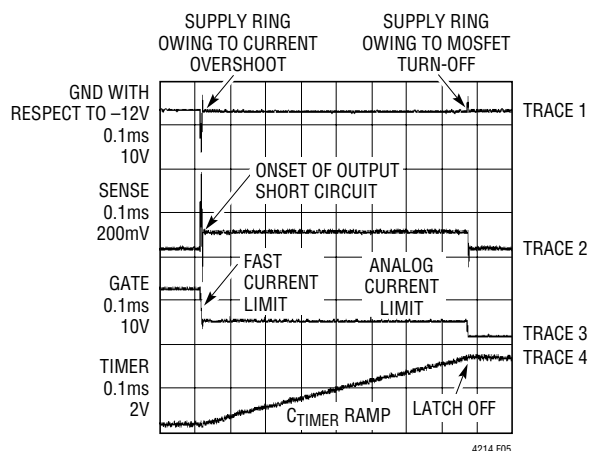


Figure 5. Output Short-Circuit Behavior of LTC4214

## APPLICATIONS INFORMATION

TIMER commences charging  $C_T$  (Trace 4) while the analog current limit loop maintains the fault current at  $70\text{mV}/R_S$ , which in this case is 3.5A (Trace 2). Note that the backplane voltage (Trace 1) sags under load. Timer pull-up is accelerated by  $V_{OUT}$ . When  $C_T$  reaches 3V, GATE turns off, PWRGD pulls high, the load current drops to zero and the backplane rings in the positive direction. The transient associated with the GATE turn off can be controlled with a snubber to reduce ringing and transient voltage suppressor to clip off large spikes. The choice of RC for the snubber is usually done experimentally. The value of the snubber capacitor is usually chosen between 10 to 100 times the MOSFET  $C_{OSS}$ . The value of the snubber resistor is typically between  $3\Omega$  to  $100\Omega$ . In many cases, a simple short-circuit test can be performed to determine the component values needed.

A low impedance short on one card may influence the behavior of others sharing the same backplane. The initial glitch and backplane sag as seen in Figure 5 Trace 1, can rob charge from output capacitors on adjacent cards. When the faulty card shuts down, current flows in to refresh the capacitors. If LTC4214s are used by the other cards, they respond by limiting the inrush current to a value of  $70\text{mV}/R_S$ . If  $C_T$  is sized correctly, the capacitors will recharge long before  $C_T$  times out.

### POWER GOOD, PWRGD

PWRGD latches low if GATE charges up to within 2.8V of  $V_{IN}$  and DRAIN pulls below  $V_{DRNL}$  during start-up. PWRGD is reset in UVLO, in a UV condition or if  $C_T$  charges up to 3V. An overvoltage condition has no effect on PWRGD status. A  $50\mu\text{A}$  current pulls this pin high during reset.

Various ways of using the PWRGD pin for interfacing with a Power Module load are shown in the Typical Application as well as Figures 2, 3, 18 and 19.

### MOSFET SELECTION

The external MOSFET switch must have adequate safe operating area (SOA) to handle short-circuit conditions

until TIMER times out. These considerations take precedence over DC current ratings. A MOSFET with adequate SOA for a given application can always handle the required current, but the opposite may not be true. Consult the manufacturer's MOSFET data sheet for safe operating area and effective transient thermal impedance curves.

MOSFET selection is a 3-step process by assuming the absence of a soft-start capacitor. First,  $R_S$  is calculated and then the time required to charge the load capacitance is determined. This timing, along with the maximum short-circuit current and maximum input voltage defines an operating point that is checked against the MOSFET's SOA curve.

To begin a design, first specify the required load current and load capacitance,  $I_L$  and  $C_L$ . The circuit breaker current trip point ( $V_{CB}/R_S$ ) should be set to accommodate the maximum load current. Note that maximum input current to a DC/DC converter is expected at  $V_{SUPPLY(MIN)}$ .  $R_S$  is given by:

$$R_S = \frac{V_{CB(MIN)}}{I_L(MAX)} \quad (8)$$

where  $V_{CB(MIN)} = 44\text{mV}$  represents the guaranteed minimum circuit breaker threshold.

During the initial charging process, the LTC4214 may operate the MOSFET in current limit, forcing ( $V_{ACL}$ ) between 60mV to 80mV across  $R_S$ . The minimum inrush current is given by:

$$I_{INRUSH(MIN)} = \frac{60\text{mV}}{R_S} \quad (9)$$

Maximum short-circuit current limit is calculated using the maximum  $V_{SENSE}$ . This gives

$$I_{SHORTCIRCUIT(MAX)} = \frac{80\text{mV}}{R_S} \quad (10)$$

The TIMER capacitor  $C_T$  must be selected based on the slowest expected charging rate; otherwise TIMER might time out before the load capacitor is fully charged. A value

## APPLICATIONS INFORMATION

for  $C_T$  is calculated based on the maximum time it takes the load capacitor to charge. That time is given by:

$$t_{CL(CHARGE)} = \frac{C \cdot V}{I} = \frac{C_L \cdot V_{SUPPLY(MAX)}}{I_{INRUSH(MIN)}} \quad (11)$$

The maximum current flowing in the DRAIN pin is given by:

$$I_{DRN(MAX)} = \frac{V_{SUPPLY(MAX)} - V_{DRNCL}}{R_D} \quad (12)$$

Approximating a linear charging rate as  $I_{DRN}$  drops from  $I_{DRN(MAX)}$  to zero, the  $I_{DRN}$  component in Equation (3) can be approximated with  $0.5 \cdot I_{DRN(MAX)}$ . Rearranging equation, TIMER capacitor  $C_T$  is given by:

$$C_T = \frac{t_{CL(CHARGE)} \cdot (40\mu A + 4 \cdot I_{DRN(MAX)})}{3V} \quad (13)$$

Returning to Equation (3), the TIMER period is calculated and used in conjunction with  $V_{SUPPLY(MAX)}$  and  $I_{SHORTCIRCUIT(MAX)}$  to check the SOA curves of a prospective MOSFET.

As a numerical design example, consider a 10W load, which requires 1.1A input current at -10.8V. If  $V_{SUPPLY(MAX)} = 13.2V$  and  $C_L = 100\mu F$ ,  $R_D = 475k$ , Equation (8) gives  $R_S = 40m\Omega$ ; Equation (13) gives  $C_T = 34nF$ . To account for errors in  $R_S$ ,  $C_T$ , TIMER current (40 $\mu A$ ), TIMER threshold (3V),  $R_D$ , DRAIN current multiplier and DRAIN voltage clamp ( $V_{DRNCL}$ ), the calculated value should be multiplied by 1.5, giving the nearest standard value of  $C_T = 56nF$ .

If a short-circuit occurs, a current of up to 80mV/40m $\Omega = 2A$  will flow in the MOSFET for 0.9ms as dictated by  $C_T = 56nF$  in Equation (3). The MOSFET must be selected based on this criterion. The IRF7413 can handle 20V and 2A for 9ms and is safe to use in this application.

Computing the maximum soft-start capacitor value during soft-start to a load short is complicated by the nonlinear MOSFET's SOA characteristics and the  $R_{SS}C_{SS}$  response. An overly conservative but simple approach begins with

the maximum circuit breaker current, given by:

$$I_{CB(MAX)} = \frac{56mV}{R_S} \quad (14)$$

From the SOA curves of a prospective MOSFET, determine the time allowed,  $t_{SOA(MAX)}$ .  $C_{SS}$  is given by:

$$C_{SS} = \frac{t_{SOA(MAX)}}{1.61 \cdot R_{SS}} \quad (15)$$

In the above example, 56mV/40m $\Omega$  gives 1.4A.  $t_{SOA(MAX)}$  for the IRF7413 is 8ms for 1.4A at 30V. From Equation (15),  $C_{SS} = 68nF$ . Actual board evaluation showed that  $C_{SS} = 33nF$  was appropriate. The ratio ( $R_{SS} \cdot C_{SS}$ ) to  $t_{CL(CHARGE)}$  is a good gauge as a large ratio may result in the time-out period expiring. This gauge is determined empirically with board level evaluation.

## SUMMARY OF DESIGN FLOW

To summarize the design flow, consider the application shown in Figure 2. It was designed for 12W for a -10V to -14V supply.

Calculate the maximum load current: 12W/10V = 1.2A; allowing for 75% converter efficiency,  $I_{IN(MAX)} = 1.6A$ .

Calculate  $R_S$ : from Equation (8)  $R_S = 25m\Omega$ .

Calculate  $I_{SHORTCIRCUIT(MAX)}$ : from Equation (10)  $I_{SHORTCIRCUIT(MAX)} = 3.2A$ .

Select a MOSFET that can handle 3.2A at 14V: IRF7413.

Calculate  $C_T$ : from Equation (13)  $C_T = 24nF$ . Select  $C_T = 47nF$ , which gives the circuit breaker time-out period  $t_{MAX} = 0.7ms$ .

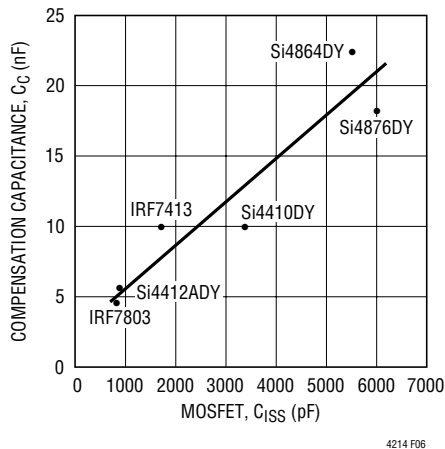
Consult MOSFET SOA curves: the IRF7413 can handle 3.2A at 20V for 3.5ms, so it is safe to use in this application.

Calculate  $C_{SS}$ : using Equations (14) and (15) select  $C_{SS} = 22nF$ .

## FREQUENCY COMPENSATION

The LTC4214 typical frequency compensation network for the analog current limit loop is a series  $R_C$  (10 $\Omega$ ) and  $C_C$  connected to  $V_{EE}$ . Figure 6 depicts the relationship be-

## APPLICATIONS INFORMATION



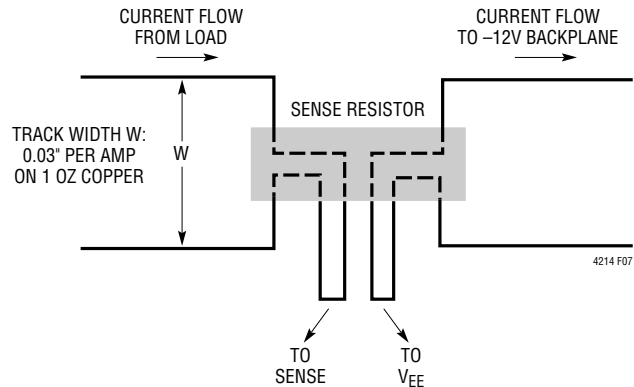
**Figure 6. Recommended Compensation Capacitor  $C_C$  vs MOSFET  $C_{ISS}$**

tween the compensation capacitor  $C_C$  and the MOSFET's  $C_{ISS}$ . The line in Figure 6 is used to select a starting value for  $C_C$  based upon the MOSFET's  $C_{ISS}$  specification. Optimized values for  $C_C$  are shown for several popular MOSFETs. Differences in the optimized value of  $C_C$  versus the starting value are small. Nevertheless, compensation values should be verified by board level short-circuit testing.

As seen in Figure 5 previously, at the onset of a short-circuit event, the input supply voltage can ring dramatically owing to series inductance. If this voltage avalanches the MOSFET, current continues to flow through the MOSFET to the output. The analog current limit loop cannot control this current flow and therefore the loop undershoots. This effect cannot be eliminated by frequency compensation. A zener diode is required to clamp the input supply voltage and prevent MOSFET avalanche.

### SENSE RESISTOR CONSIDERATIONS

For proper circuit breaker operation, Kelvin-sense PCB connections between the sense resistor and the LTC4214's  $V_{EE}$  and SENSE pins are strongly recommended. The drawing in Figure 7 illustrates the correct way of making connections between the LTC4214 and the sense resistor. PCB layout should be balanced and symmetrical to minimize wiring errors. In addition, the PCB layout for the sense resistor should include good thermal management techniques for optimal sense resistor power dissipation.



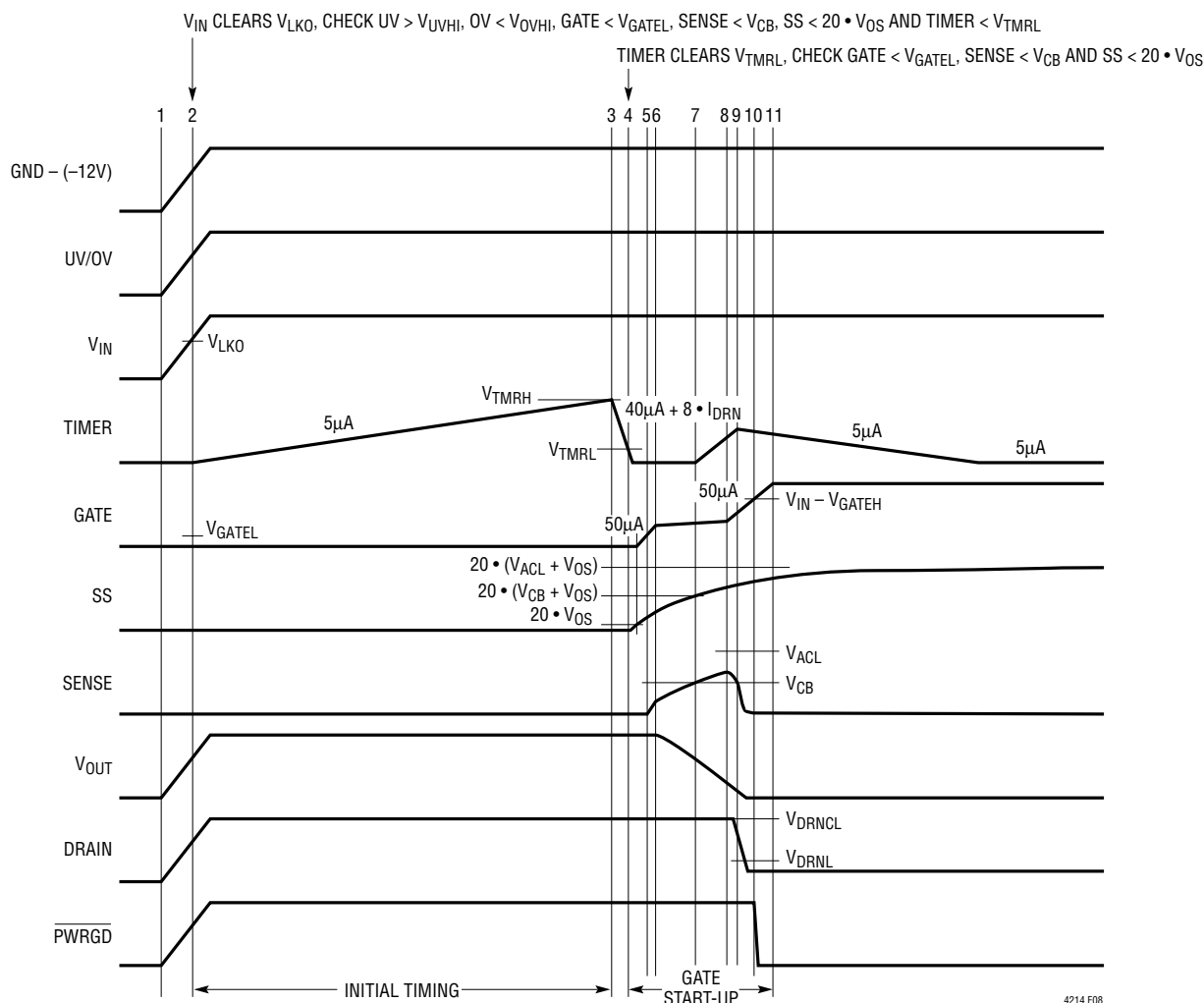
**Figure 7. Making PCB Connections to the Sense Resistor**

## TIMING WAVEFORMS

### System Power-Up

Figure 8 details the timing waveforms for a typical power-up sequence in the case where a board is already installed in the backplane and system power is applied abruptly. At time point 1, the supply ramps up, together with UV/OV,  $V_{IN}$ ,  $V_{OUT}$ , DRAIN and PWRGD. At time point 2,  $V_{IN}$  exceeds  $V_{LKO}$  and the internal logic checks for  $UV > V_{UVHI}$ ,  $OV < V_{OVHI}$ ,  $GATE < V_{GATEL}$ ,  $SENSE < V_{CB}$ ,  $SS < 20 \cdot V_{OS}$  and  $TIMER < V_{TMRL}$ . If all conditions are met, an initial timing cycle starts and the TIMER capacitor is charged by a  $5\mu A$  current source pull-up. At time point 3, TIMER reaches the  $V_{TMRH}$  threshold and the initial timing cycle terminates. The TIMER capacitor is quickly discharged. At time point 4, the  $V_{TMRL}$  threshold is reached and the conditions of  $GATE < V_{GATEL}$ ,  $SENSE < V_{CB}$  and  $SS < 20 \cdot V_{OS}$  must be satisfied before a GATE ramp-up cycle begins. SS ramps up as dictated by  $R_{SS} \cdot C_{SS}$  (as in Equation 6); GATE is held low by the analog current limit (ACL) amplifier until SS crosses  $20 \cdot V_{OS}$ . Upon releasing GATE,  $50\mu A$  sources into the external MOSFET gate and compensation network. When the GATE voltage reaches the MOSFET's threshold, current begins flowing into the load capacitor at time point 5. At time point 6, load current reaches the SS control level and the analog current limit loop activates. Between time points 6 and 8, the GATE voltage is servoed, the SENSE voltage is regulated at  $V_{ACL}(t)$  (Equation 7) and soft-start limits the slew rate of

## APPLICATIONS INFORMATION

Figure 8. System Power-Up Timing (All Waveforms are Referenced to  $V_{EE}$ )

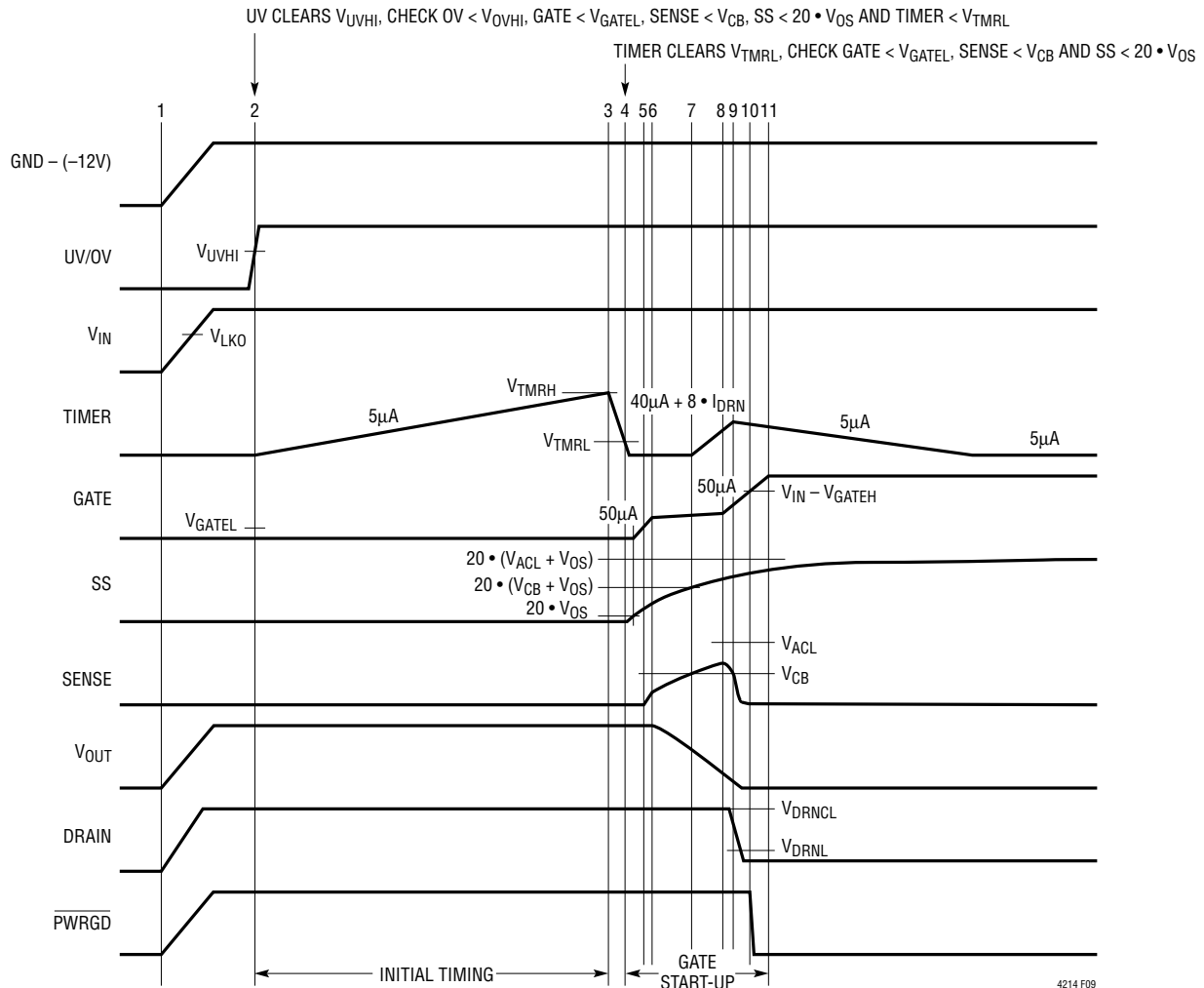
the load current. If the SENSE voltage ( $V_{SENSE} - V_{EE}$ ) reaches the  $V_{CB}$  threshold at time point 7, the circuit breaker TIMER activates. The TIMER capacitor,  $C_T$ , is charged by a  $(40\mu A + 8 \cdot I_{DRN})$  current pull-up. As the load capacitor nears full charge, load current begins to decline. At time point 8, the load current falls and the SENSE voltage drops below  $V_{ACL}(t)$ . The analog current limit loop shuts off and the GATE pin ramps further. At time point 9, the SENSE voltage drops below  $V_{CB}$ , the fault TIMER cycle ends, followed by a  $5\mu A$  discharge cycle (cool off). The duration between time points 7 and 9 must be shorter than one circuit breaker delay to avoid a fault time out during

GATE ramp-up. When GATE ramps past the  $V_{GATEH}$  threshold at time point 10, PWRGD pulls low. At time point 11, GATE reaches its maximum voltage as determined by  $V_{IN}$ .

## Live Insertion with Short Pin Control of UV/OV

In the example shown in Figure 9, power is delivered through long connector pins whereas the UV/OV divider makes contact through a short pin. This ensures the power connections are firmly established before the LTC4214 is activated. At time point 1, the power pins make contact and  $V_{IN}$  ramps through  $V_{LKO}$ . At time point 2, the UV/OV divider

## APPLICATIONS INFORMATION

Figure 9. Power-Up Timing with a Short Pin (All Waveforms are Referenced to  $V_{EE}$ )

makes contact and its voltage exceeds  $V_{UVHI}$ . In addition, the internal logic checks for  $OV < V_{OVHI}$ ,  $GATE < V_{GATEL}$ ,  $SENSE < V_{CB}$ ,  $SS < 20 \cdot V_{OS}$  and  $TIMER < V_{TMRL}$ . If all conditions are met, an initial timing cycle starts and the TIMER capacitor is charged by a  $5\mu A$  current source pull-up. At time point 3, TIMER reaches the  $V_{TMRH}$  threshold and the initial timing cycle terminates. The TIMER capacitor is quickly discharged. At time point 4, the  $V_{TMRL}$  threshold is reached and the conditions of  $GATE < V_{GATEL}$ ,  $SENSE < V_{CB}$  and  $SS < 20 \cdot V_{OS}$  must be satisfied before a GATE start-up cycle begins. SS ramps up as dictated by  $R_{SS} \cdot C_{SS}$ ; GATE is held low by the analog current limit

amplifier until SS crosses  $20 \cdot V_{OS}$ . Upon releasing GATE,  $50\mu A$  sources into the external MOSFET gate and compensation network. When the GATE voltage reaches the MOSFET's threshold, current begins flowing into the load capacitor at time point 5. At time point 6, load current reaches the SS control level and the analog current limit loop activates. Between time points 6 and 8, the GATE voltage is servoed, the SENSE voltage is regulated at  $V_{ACL}(t)$  and soft-start limits the slew rate of the load current. If the SENSE voltage ( $V_{SENSE} - V_{EE}$ ) reaches the  $V_{CB}$  threshold at time point 7, the circuit breaker TIMER activates. The TIMER capacitor,  $C_T$ , is charged by a

## APPLICATIONS INFORMATION

$(40\mu\text{A} + 8 \cdot I_{\text{DRN}})$  current pull-up. As the load capacitor nears full charge, load current begins to decline. At point 8, the load current falls and the SENSE voltage drops below  $V_{\text{ACL}}(t)$ . The analog current limit loop shuts off and the GATE pin ramps further. At time point 9, the SENSE voltage drops below  $V_{\text{CB}}$  and the fault TIMER cycle ends, followed by a  $5\mu\text{A}$  discharge cycle (cool off). When GATE ramps past  $V_{\text{GATEH}}$  threshold at time point 10,  $\overline{\text{PWRGD}}$  pulls low. At time point 11, GATE reaches its maximum voltage as determined by  $V_{\text{IN}}$ .

### Undervoltage Timing

In Figure 10 when the UV pin drops below  $V_{\text{UVHI}} - V_{\text{UVHST}}$  (time point 1), the LTC4214 shuts down with TIMER, SS and GATE all pulling low. If current has been flowing, the SENSE pin voltage decreases to zero as GATE collapses. When UV recovers and clears  $V_{\text{UVHI}}$  (time point 2), an initial timer cycle begins followed by a start-up cycle.

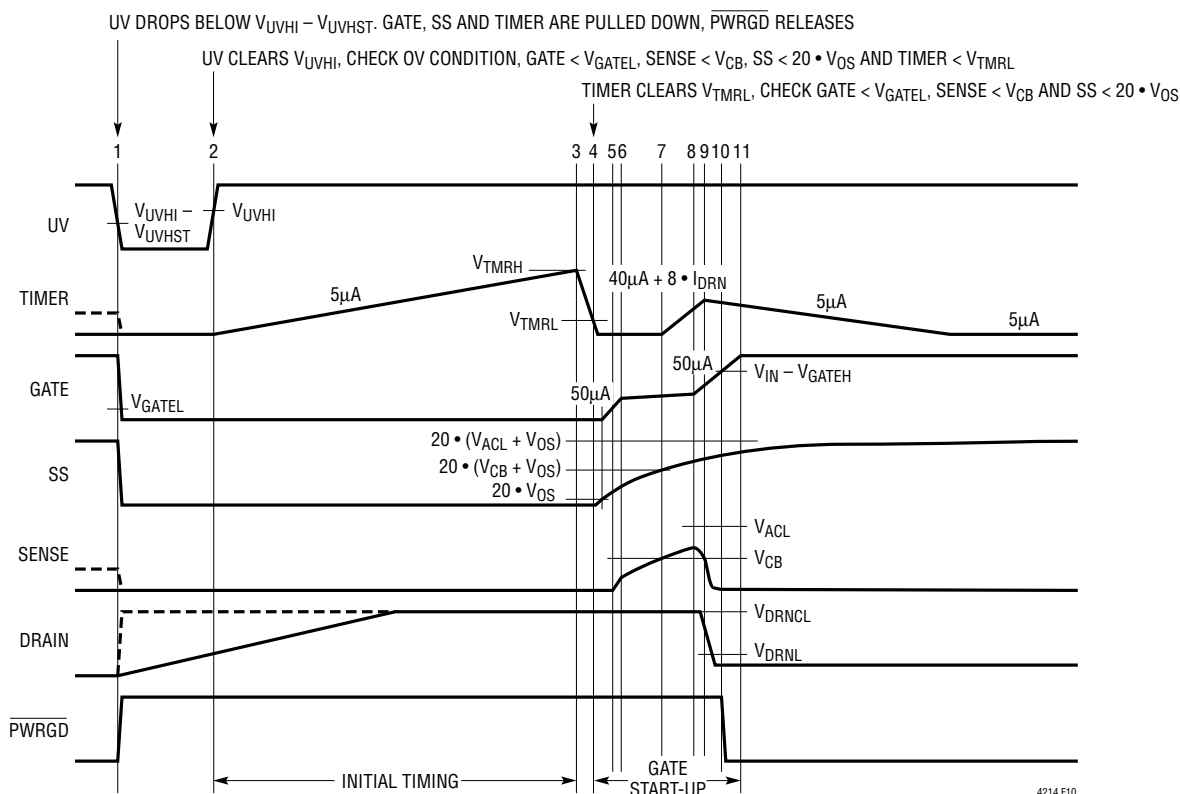


Figure 10. Undervoltage Timing (All Waveforms are Referenced to  $V_{\text{EE}}$ )

4214 F10

## APPLICATIONS INFORMATION

### $V_{IN}$ Undervoltage Lockout Timing

The  $V_{IN}$  undervoltage lockout comparator, UVLO, has a similar timing behavior as the UV pin timing except it looks for  $V_{IN} < (V_{LKO} - V_{LKH})$  to shut down and  $V_{IN} > V_{LKO}$  to start. In an undervoltage lockout condition, both UV and OV comparators are held off. When  $V_{IN}$  exits undervoltage lockout, the UV and OV comparators are enabled.

### Undervoltage Timing with Overvoltage Glitch

In Figure 11, both UV and OV pins are connected together. When UV clears  $V_{UVHI}$  (time point 1), an initial timing cycle starts. If the system bus voltage overshoots  $V_{OVHI}$  as shown at time point 2, TIMER discharges. At time point 3, the supply voltage recovers and drops below the  $V_{OVHI} - V_{OVHST}$  threshold. The initial timing cycle restarts, followed by a GATE start-up cycle.

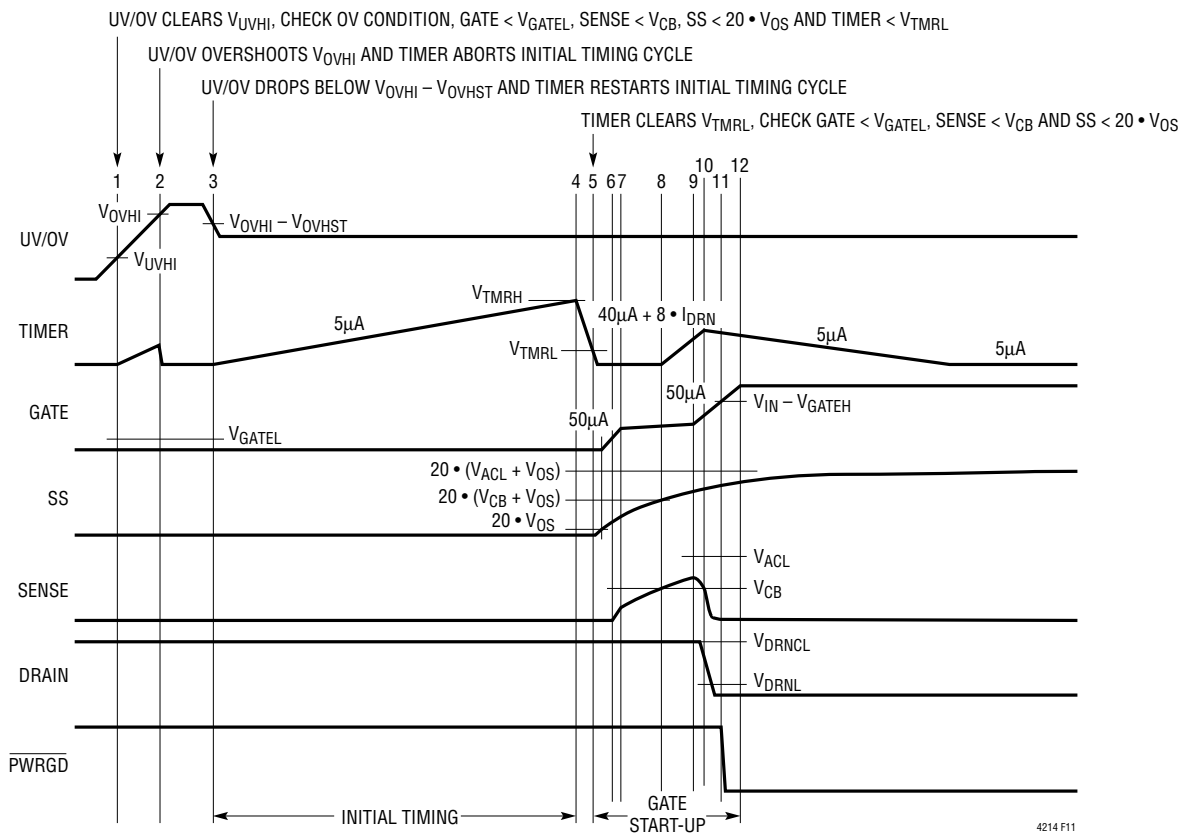


Figure 11. Undervoltage Timing with an Overvoltage Glitch (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Overvoltage Timing

During normal operation, if the OV pin exceeds  $V_{OVHI}$  as shown at time point 1 of Figure 12, the TIMER and PWRGD status are unaffected. Nevertheless, SS and GATE pull down and the load is disconnected. At time point 2, OV

recovers and drops below the  $V_{OVHI} - V_{OVHST}$  threshold. A GATE start-up cycle begins. If the overvoltage glitch is long enough to deplete the load capacitor, a full start-up cycle as shown between time points 4 through 7 may occur.

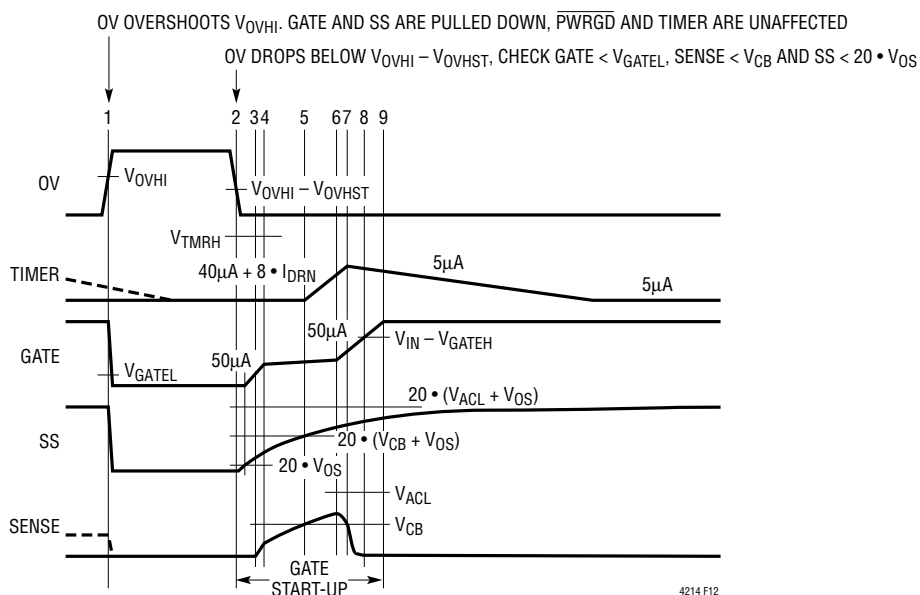


Figure 12. Overvoltage Timing (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Circuit Breaker Timing

In Figure 13a, the TIMER capacitor charges at  $40\mu\text{A}$  if the SENSE pin exceeds  $V_{CB}$  but  $V_{DRN}$  is less than  $4.2\text{V}$ . If the SENSE pin drops below  $V_{CB}$  before TIMER reaches the  $V_{TMRH}$  threshold, TIMER is discharged by  $5\mu\text{A}$ . In Figure 13b, when TIMER exceeds  $V_{TMRH}$ , GATE pulls down

immediately and the LTC4214 shuts down. In Figure 13c, multiple momentary faults cause the TIMER capacitor to integrate and reach  $V_{TMRH}$ . GATE pull down follows and the LTC4214 shuts down. During shutdown, the LTC4214-1 latches TIMER high with a  $5\mu\text{A}$  pull-up current source; the LTC4214-2 activates a shutdown cooling cycle.

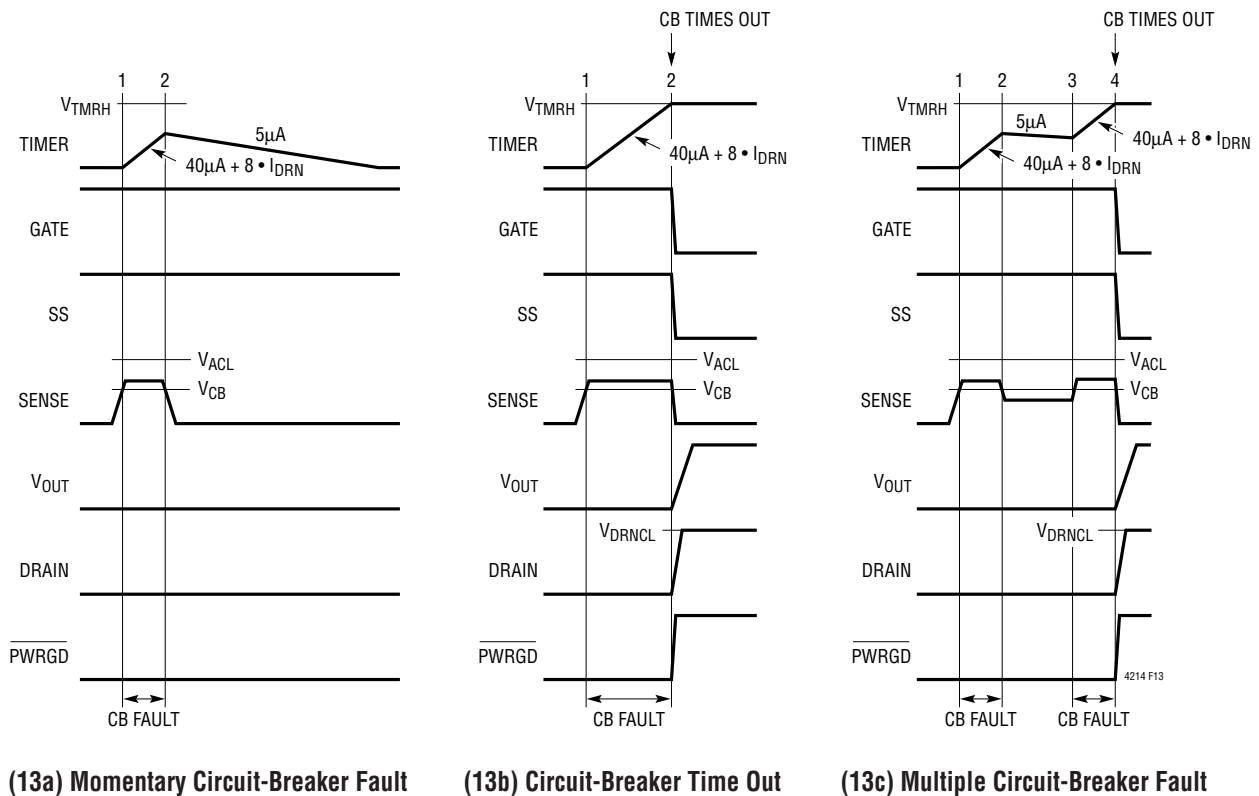


Figure 13. Circuit-Breaker Timing Behavior (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Resetting a Fault Latch (LTC4214-1)

The latched circuit breaker fault of LTC4214-1 benefits from long cooling time. It is reset by pulling the UV pin below  $V_{UVHI} - V_{UVHST}$  with a switch. Reset is also accomplished by pulling the  $V_{IN}$  pin momentarily below  $(V_{LKO} - V_{LKH})$ . A third reset method involves pulling the TIMER pin below  $V_{TMRL}$  as shown in Figure 14. An initial timing cycle is skipped if TIMER is used for reset. An initial timing cycle is generated if reset by the UV pin or the  $V_{IN}$  pin.

The duration of the TIMER reset pulse should be smaller than the time taken to reach 0.2V at SS pin. With a single pole mechanical pushbutton switch, this may not be feasible. A double pole, single throw pushbutton switch removes this restriction by connecting the second switch to the SS pin. With this method, both the SS and TIMER pins are released at the same time.

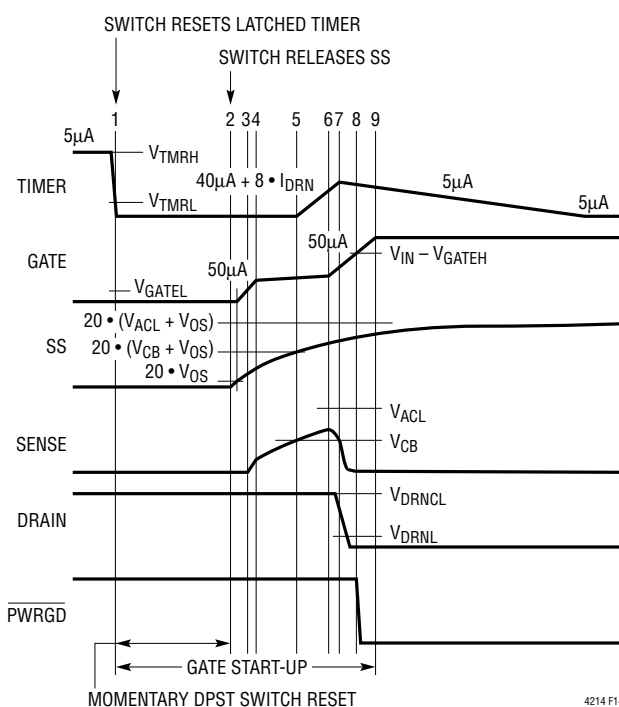


Figure 14. Pushbutton Reset of LTC4214-1's Latched Fault (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Shutdown Cooling Cycle (LTC4214-2)

Figure 15 shows the timer behavior of the LTC4214-2. At time point 2, TIMER exceeds  $V_{TMRH}$ , GATE pulls down immediately and the LTC4214 shuts down. TIMER starts a shutdown cooling cycle by discharging TIMER with  $5\mu A$  to the  $V_{TMRH}$  threshold. TIMER then charges with  $5\mu A$  to the  $V_{TMRH}$  threshold. There are four  $5\mu A$  discharge phases

and three  $5\mu A$  charge phases in this shutdown cooling cycle spanning time points 2 and 3. At time point 3, the LTC4214 automatic retry occurs with a start-up cycle. Good thermal management techniques are highly recommended; power and thermal dissipation must be carefully evaluated when implementing the automatic retry scheme.

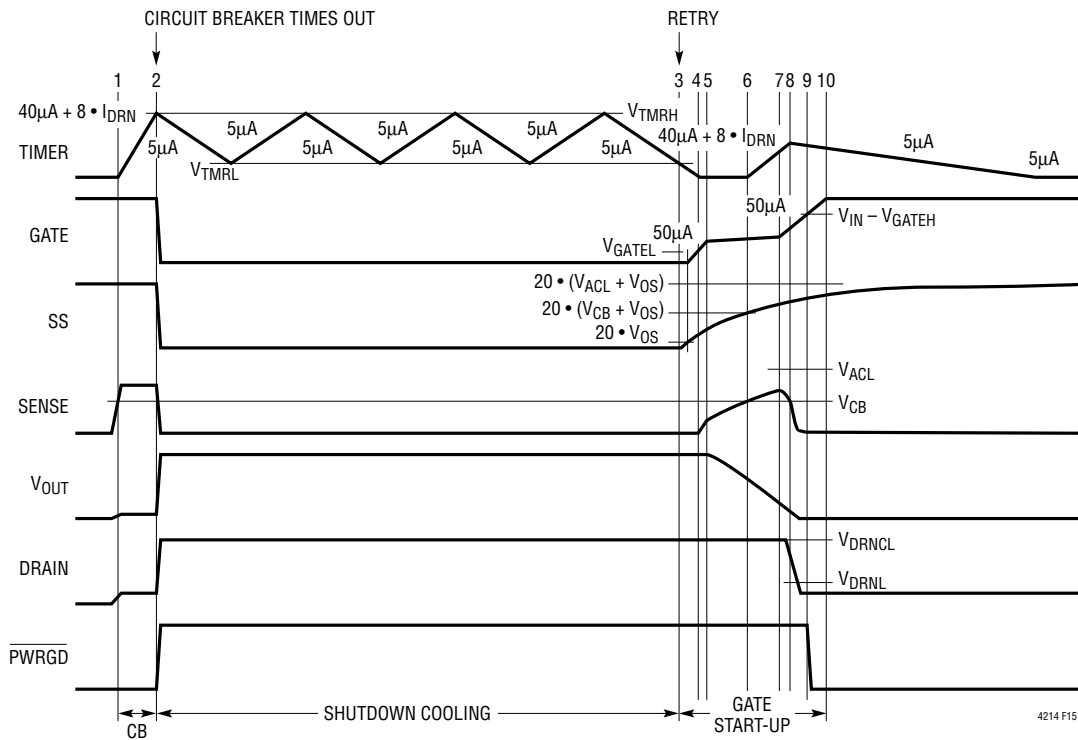


Figure 15. Shutdown Cooling Timing Behavior of LTC4214-2 (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Analog Current Limit and Fast Current Limit

In Figure 16a, when SENSE exceeds  $V_{ACL}$ , GATE is regulated by the analog current limit amplifier loop. When SENSE drops below  $V_{ACL}$ , GATE is allowed to pull up. In Figure 16b, when a severe fault occurs, SENSE exceeds  $V_{FCL}$  and GATE immediately pulls down until the analog current amplifier can establish control. If the severe fault

causes  $V_{OUT}$  to exceed  $V_{DRNCL}$ , the DRAIN pin is clamped at  $V_{DRNCL}$ .  $I_{DRN}$  flows into the DRAIN pin and is multiplied by 8. This extra current is added to the TIMER pull-up current of  $40\mu A$ . This accelerated TIMER current of  $[40\mu A + 8 \cdot I_{DRN}]$  produces a shorter circuit breaker fault delay. Careful selection of  $C_T$ ,  $R_D$  and MOSFET can help prevent SOA damage in a low impedance fault condition.

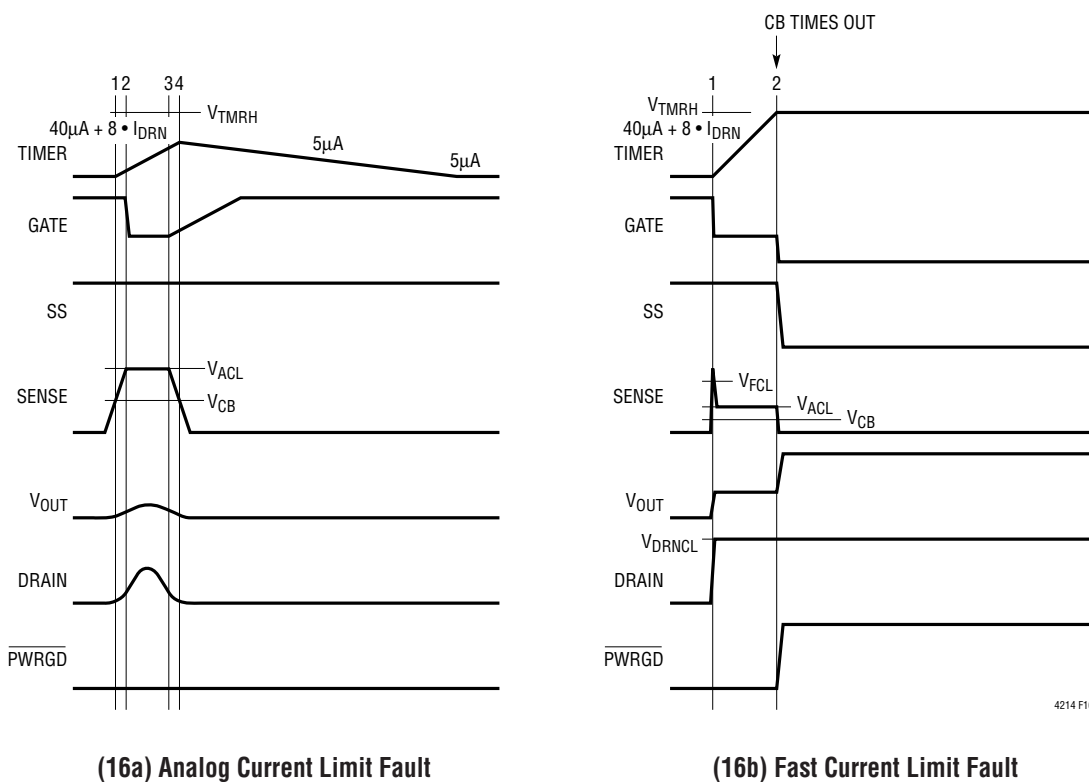


Figure 16. Current Limit Behavior (All Waveforms are Referenced to  $V_{EE}$ )

## APPLICATIONS INFORMATION

### Soft-Start

If the SS pin is not connected, this pin defaults to a linear voltage ramp, from 0V to 1.6V in about 220 $\mu$ s at GATE start-up, as shown in Figure 17a. If a soft-start capacitor,  $C_{SS}$ , is connected to this SS pin, the soft-start response is modified from a linear ramp to an RC response (Equation 6), as shown in Figure 17b. This feature allows load current to slowly ramp-up at GATE start-up. Soft-start is initiated at time point 3 by a TIMER transition from  $V_{TMRH}$  to  $V_{TMRL}$  (time points 1 to 2) or by the OV pin falling below the  $V_{OVHI} - V_{OVHST}$  threshold after an OV condition. When the SS pin is below 0.2V, the analog current limit amplifier holds GATE low. Above 0.2V, GATE is released and 50 $\mu$ A ramps up the compensation network and GATE capacitance at time point 4. Meanwhile, the SS pin voltage continues to ramp up. When GATE reaches the MOSFET's threshold, the MOSFET begins to conduct. Due to the MOSFET's high  $g_m$ , the MOSFET current quickly reaches

the soft-start control value of  $V_{ACL}(t)$  (Equation 7). At time point 6, the GATE voltage is controlled by the current limit amplifier. The soft-start control voltage reaches the circuit breaker voltage,  $V_{CB}$ , at time point 7 and the circuit breaker TIMER activates. As the load capacitor nears full charge, load current begins to decline below  $V_{ACL}(t)$ . The current limit loop shuts off and GATE releases at time point 8. At time point 9, the SENSE voltage falls below  $V_{CB}$  and TIMER deactivates.

Large values of  $C_{SS}$  can cause premature circuit breaker time out as  $V_{ACL}(t)$  may exceed the  $V_{CB}$  potential during the circuit breaker delay. The load capacitor is unable to achieve full charge in one GATE start-up cycle. A more serious side effect of large  $C_{SS}$  values is SOA duration may be exceeded during soft-start into a low impedance load. A soft-start voltage below  $V_{CB}$  will not activate the circuit breaker TIMER.

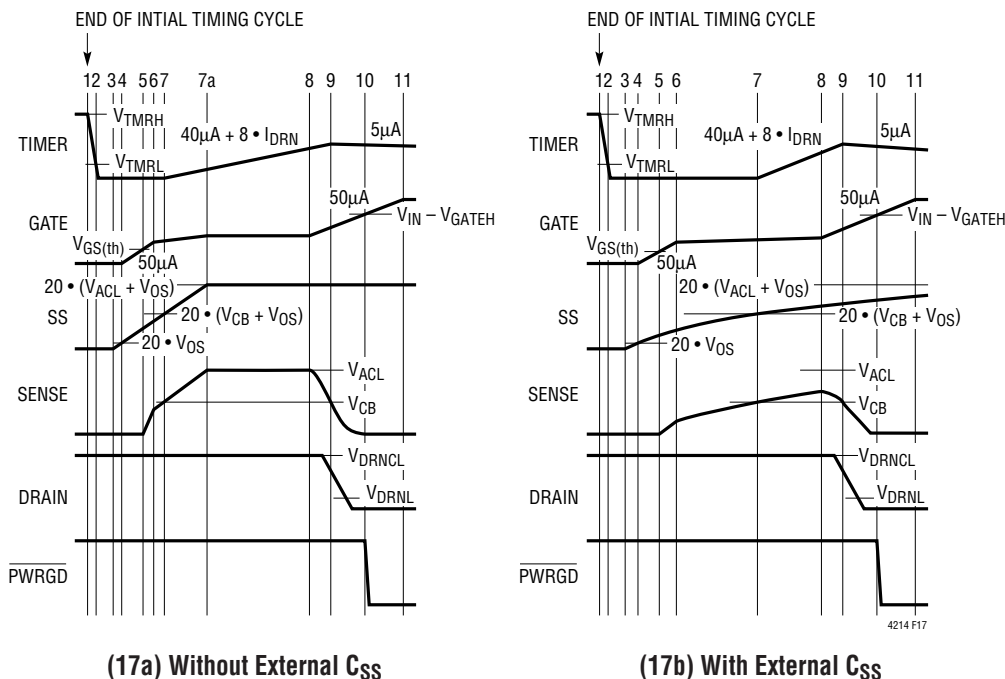


Figure 17. Soft-Start Timing (All Waveforms are Referenced to  $V_{EE}$ )

Figure 18 shows the LTC4214-1 in a power limit circuit breaking application. The SENSE pin is modulated by the board supply voltage,  $V_{\text{SUPPLY}}$ . The zener voltage,  $V_Z$  is set to be the same as the low supply operating voltage,  $V_{\text{SUPPLY(MIN)}} = 10\text{V}$ . If the goal is to have the high supply operating voltage,  $V_{\text{SUPPLY(MAX)}} = 14\text{V}$  give the same power at  $V_{\text{SUPPLY(MIN)}}$ , then resistors R4 and R6 are selected using the ratio:

If R6 is 20Ω, R4 is 5.6k. The peak circuit breaker power limit is:

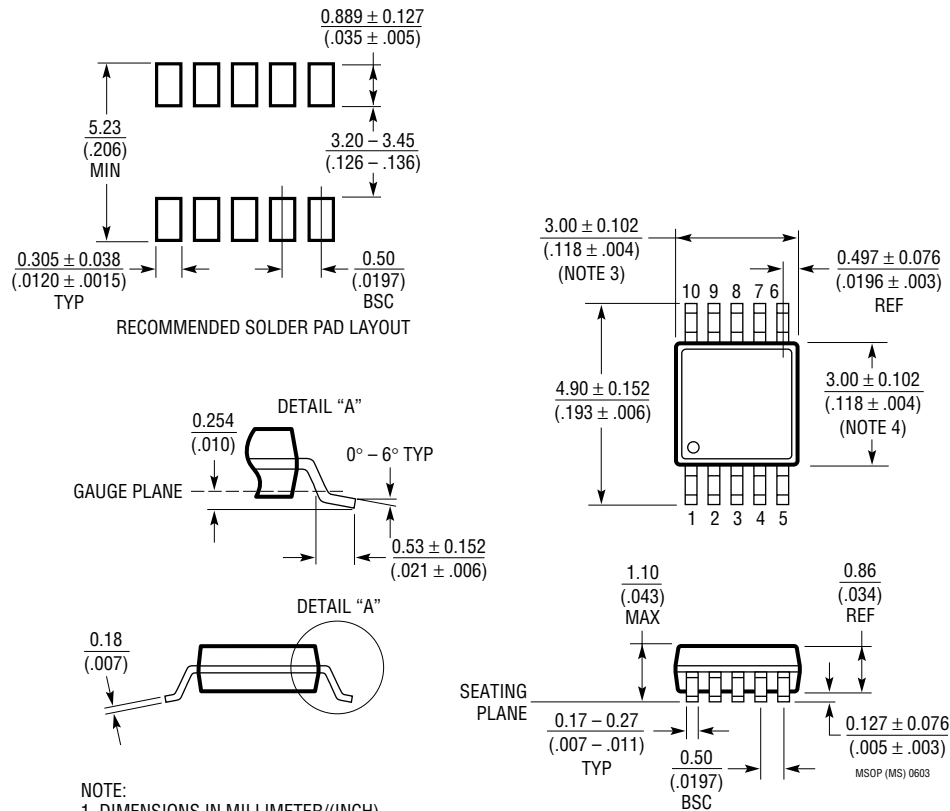
The peak power at the fault current limit occurs at the supply overvoltage threshold. The fault current limited power is:

$$\text{POWER}_{\text{FAULT}} = \frac{V_{\text{SUPPLY}}}{R_s} \cdot \left( V_{\text{ACL}} - (V_{\text{SUPPLY}} - V_Z) \cdot \frac{R_6}{R_4} \right) \quad (18)$$



# PACKAGE DESCRIPTION

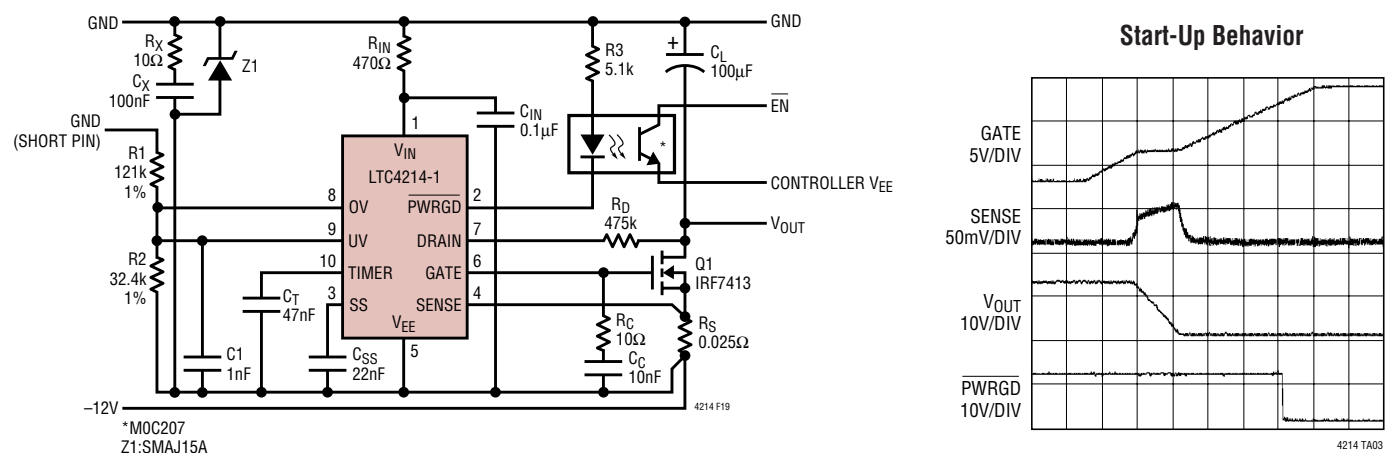
**MS Package**  
**10-Lead Plastic MSOP**  
 (Reference LTC DWG # 05-08-1661)



## NOTE:

1. DIMENSIONS IN MILLIMETER/(INCH)
2. DRAWING NOT TO SCALE
3. DIMENSION DOES NOT INCLUDE MOLD FLASH, PROTRUSIONS OR GATE BURRS.  
MOLD FLASH, PROTRUSIONS OR GATE BURRS SHALL NOT EXCEED 0.152mm (.006") PER SIDE
4. DIMENSION DOES NOT INCLUDE INTERLEAD FLASH OR PROTRUSIONS.  
INTERLEAD FLASH OR PROTRUSIONS SHALL NOT EXCEED 0.152mm (.006") PER SIDE
5. LEAD COPLANARITY (BOTTOM OF LEADS AFTER FORMING) SHALL BE 0.102mm (.004") MAX

TYPICAL APPLICATION



RELATED PARTS

PART NUMBER	DESCRIPTION	COMMENTS
LTC1421	Two Channels, Hot Swap Controller	Operates from 3V to 12V and Supports -12V
LTC1642	Fault Protected Hot Swap Controller	3V to 16.5V, Overvoltage Protection up to 33V
LTC1644	PCI Hot Swap Controller	3.3V, 5V and ±12V; 1V Precharge; PCI Reset Logic
LTC4210	Hot Swap Controller in SOT-23	Active Current Limiting, 2.7V to 16.5V
LTC4211	Single Hot Swap with Multifunction Current Control	Operates from 2.5V to 16.5V
LT4220	Dual Hot Swap Controller for Positive/Negative Supplies	Operates from ±2.7V to ±16.5V
LTC4230	Triple Hot Swap Controller with Multifunction Current Control	Operates from 1.7V to 16.5V